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TABLE OF CONTENTS

			<u>Page</u>
LIST	OF F	IGURES	v
LIST	OF TA	ABLES	vii
1.	INTR	DDUCTION	1
II.	ASAR	SIMULATION EFFORTS	3
	A.	Discussion	3
	В.	Dynamics Simulation	3
	c.	Radar Simulation	5
	D.	Antenna Simulation	8
	E.	Terrain Specifications	8
111.	OTHE	R SIMULATION INVESTIGATIONS	13
	A.	Antenna Polarization Effect	13
	в.	Frequency Diversity Effects	25
IV.	TECH	NICAL EFFORT SUMMARY	31

LIST OF FIGURES

Title	Page
Simulation Architecture	14
Imagery from ARL:UT Synthetic Aperture Radar (SAR) Math Model	15
Polarization Ellipse	17
APQ-102 Antenna Simulation Patterns	21
OSS Simulation of Six-Scatterer Array Using SEASAT System with APQ-102 Antenna Pattern in Azimuth, No Pulse Compression	22
OSS Simulation of Six-Scatterer Array Using SEASAT System with Unit Antenna Pattern in Azimuth, No Pulse Compression	23
Ambiguity Terrain	24
Results from SAR Simulation Program	26
Test Scene, Wavelength Diversity	28
ARL:UT High Resolution Display System	30
The Geometry of the Multiple Beam SAR	32
	TitleSimulation ArchitectureImagery from ARL:UT Synthetic Aperture Radar (SAR) Math ModelPolarization EllipseAPQ-102 Antenna Simulation PatternsOSS Simulation of Six-Scatterer Array Using SEASAT System with APQ-102 Antenna Pattern in Azimuth, No Pulse CompressionOSS Simulation of Six-Scatterer Array Using SEASAT System with Unit Antenna Pattern in Azimuth, No Pulse CompressionAmbiguity Terrain Results from SAR Simulation Program Test Scene, Wavelength Diversity ARL:UT High Resolution Display System The Geometry of the Multiple Beam SAR

LIST OF TABLES

<u>Table</u>	Title	Page
I	RADAR SPECIFICATIONS RADAR ID: ASAR 1	7
11	ANTENNA SPECIFICATIONS	9
III	TERRAIN SPECIFICATIONS	10
IV	PARTIAL RESULTS OF FREQUENCY DIVERSITY STUDY	29

I. INTRODUCTION

The contract was initially oriented toward simulating the radar parameters of the ASAR (Advanced Synthetic Aperture Radar) system under development jointly by NASA/JPL and NASA/JSC. The former had been tasked to develop a system using a technique known as "burst mode" with wavelength diversity in pulse bursts of transmissions. NASA/JSC was responsible for developing the antenna system required for handling the wide band of frequencies involved. The ARL:UT supporting effort was to simulate the system design and particularly the "burst mode", to provide insight into the operation of the algorithms and anticipated results. The simulation developed by ARL:UT for an orbiting SAR platform had to be modified to support the aircraft based ASAR.

After three months of effort toward these objectives, a decision was made to stop further work on the ASAR system and instead concentrate on certain key SAR technology areas. Among these are multi-olarization antennas, multifrequency radar, multibeam squint mode SAR (wide swath), calibration techniques, and burst mode implementation. Of these, ARL:UT addressed the first three in varying degree.

II. ASAR SIMULATION EFFORTS

A. Discussion

The ARL:UT orbital SAR simulation (OSS) had to be modified to simulate an aircraft flying in earth's atmosphere at a relatively low velocity and altitude compared to the orbiting platform. In addition, the radar parameters had to be obtained from the syster designers at NASA/JPL and the antenna parameters from the project personnel at NASA/JSC. The system was to have exhibited two unique design features: extremely broad wavelength coverage, and data processing of synthetic data arrays formed by bursts of pulses at several different radar frequencies.

The purposes of the simulation were to investigate and demonstrate the validity of the system design, in particular the so-called "burst mode" operation.

Two sets of problems were encountered in this effort. The first had to do with adapting the existing simulation, of a space-based orbiting radar, to the aircraft-based design. This problem set was rather easily solved, but attempts to define the design parameters of the radar system were relatively unsuccessful initially, and two or three months elapsed before a preliminary set of parameters for use in the simulation was agreed upon and obtained.

B. Dynamics Simulation

In order to utilize the existing routines in the simulation, the proposed aircraft platform (a CV 990) was considered like an orbiting platform in a low earth gravity environment, so that

3

it could maintain orbit at its usual altitude and velocity. The magnitude of the velocity vector is

$$V_s = a(1-e^2\cos^2 E)^{1/2} \cdot \dot{E}$$
, (1)

with the altitude specified by the orbit radius from earth's center

$$r_s = a(1 - e \cos E) \qquad (2)$$

The gravitational constant of earth μ_p has been measured at 398,601 km³/sec². In Eq. (2) e is the eccentricity of the orbit, and E is the eccentric anomaly. If e is zero, the orbit is circular. The parameter a is the semimajor axis of the orbit ellipse, or the radius of the orbit with e=0.

By selecting the proper values for the six Kepler orbital elements, a, e, i, Ω , ω , and T_p, the orbit is specified. In Eq. (1), È is the time derivative of the eccentric anomaly:

$$E - e \sin E = v(t-T_p)$$
(3)

$$\frac{dE}{dt} (1 - e \cos E) = v \qquad (4)$$

Here v is the mean angular velocity of the platform

$$v = \sqrt{\frac{\mu_p}{a^3}} \qquad (5)$$

In order to derive a usable value of μ_p we can simplify the operation by assuming a spherical earth and a circular orbit for the aircraft. We find that

$$r_s = a$$
, $v_s = a \times \dot{E}$, $\dot{E} = v$; (6)

therefore

$$V_{s} = r_{s}v = a(\mu_{p}/a^{3})^{1/2} = (\mu_{p}/a)^{1/2}$$
 (7)

Assuming that the CV 990 will fly at 400 kt TAS (205 m/sec) at an altitude of 12,000 m (39,372 ft), we can solve for an imaginary value of $\mu_{\rm p}$ which will provide the proper angular rate.

$$\mu_{p} = aV_{s}^{2}$$

$$= (0.205)^{2} (12+6378.167)$$

$$= 268.2 \text{ km}^{3}/\text{sec}^{2} ,$$
(8)

compared with the measured value for earth cf

$$\mu_p = 398,601 \text{ km}^3/\text{sec}^2$$

All other planet earth parameters remain the same.

For the orbit specification, all parameters used for SEASAT, for example, can remain the same except the semimajor axis a, which becomes 6390.167 km (12+6378.167) and the orbit rotational rate n, which becomes

$$\frac{1}{2\pi} \frac{V_{s}}{r_{s}} = \frac{1}{2\pi} \left(\frac{0.205}{6390.167} \right) = 18.4 \times 10^{-4} \text{ deg/sec}$$

.

C. Radar Simulation

The proposed ASAR design was to have used linear FM (chirp) pulse compression, whereas the OSS is designed for binary phase coded pulse compression, which is particularly adapted to digital processing. Some effort was spent in analyzing the pulse compression routine requirements to provide an analogous digital signal sampled at the Nyquist rate.

Following a specification review at JSC, a first attempt was made to assign radar specification values for the simulation. Table I contains most of these values.

The linear FM chirp modulation proposed for the ASAR has the following parameters.

$$f_0 = 10^9 \text{ Hz}$$
; $f_1 = 1.02 \times 10^9 \text{ Hz}$, $\frac{df}{dt} = 10^{12} \text{ Hz/sec}^2$
T = 20 × 10⁻⁶ sec .

The equation for the phase as a function of time is

$$\phi = \phi_{0} + f_{0}t + \frac{1}{2}\frac{df}{dt}t^{2} , \quad \phi_{0} = 0 \text{ rad}$$
(9)
at $t = 0 , \quad \phi = \phi_{0} = 0$
at $t = n , \quad \phi_{n} = \phi_{0} + f_{0}(n) + \frac{1}{2}\frac{df}{dt}(n)^{2}$
at $t = n-1 , \quad \phi_{n-1} = \phi_{0} + f_{0}(n-1) + \frac{1}{2}\frac{df}{dt}(n-1)^{2} .$
If $\Delta t = n - (n-1) = 1 , \quad \Delta \phi = \phi_{1} - \phi_{n-1} = f_{0} + \frac{1}{2}\frac{df}{dt}(2n-1) .$

From the sampling theorem, sampling period = 1/2 period of highest frequency,

let
$$\Delta t = \frac{1}{2f_1} [n-(n-1)] = \frac{1}{2f_1} = \frac{1}{2.04 \times 10^9} = 0.49 \text{ nsec}$$
, (10)

then

$$\phi_n = \phi_0 + n\Delta t f_0 + \frac{1}{2} \frac{df}{dt} (n\Delta t)^2$$
(11)

$$\phi_{n-1} = \phi_0 + (n-1)\Delta t f_0 + \frac{1}{2} \frac{df}{dt} (n-1)^2 \Delta t^2$$
 (12)

TABLE I

	-	
Radar Specifications Rad	lar ID:	ASAR 1

			L	S	C	<u>X</u>
	λ	WL	Radar wavelength, m 0.2353	13 0.093685	0.06245	0.03
	TB	TBW	Range time-bandwidth produ	ct	400	
		S/N	Received signal-to-noise r	atio, dB	7.0	
	N P	LRC	Sample length of range cor	relation 4	0,800	
	n s	LPI	Sample length across phase	interval	1	
	°r	RESR	Ground range resolution, m	:	25 √2	
	ρ _a	RESA	Azimuth resolution, m		2	
	s r	SRR	Range sampling ratio		1	
		крс	Phase code, $v_n = 10^{-3}\pi [0.98]$	+ (2n-1) 0.2	4×10^{-3}]	rad
		KPCS	Phase code sequence, BCD		1	
	s a	SRA	Azimuth sampling ratio		1	
*		KRFTNR	Name of range impulse resp	onse function	, BCD: c	osine ²
*		KWTFTNA	Name of aperture weighting	function, BC	D T	aylor
*		SHADFAC	Aperture weight factor		-	30 dB
	POR	PCOFFR	Patch-to-patch offset, ran	ge, m		0
	POA	PCOFFA	Patch-to-patch offset, azis	muth, m		0
	SW	SW	Swath width, km			26
		NA	Number of patches			1
	LAT	STLAT	Map start latitude, rad		2π	/10
	rt	TCR	Planetocentric distance to	terrain cent 0.0	er, km 636751923	70 × 10 ⁴
	LTt	TCLAT	Terrain center latitude, ra	ad	2π	/10
	LNt	TCLONG	Terrain center longitude,	rad	π	

7

$$\Delta \phi_{n} = \phi_{n} - \phi_{n-1} = \Delta t f_{0} + \frac{1}{2} \frac{df}{dt} [(n\Delta t^{2}) - (n\Delta t)^{2} + (2n-1)\Delta t^{2}]$$

$$= \Delta t f_{0} + \frac{1}{2} \frac{df}{dt} (2n-1)\Delta t^{2} \text{ cycles}$$

$$= 2\pi f_{0}\Delta t + \pi \frac{df}{dt} (2n-1)\Delta t^{2} \text{ rad}$$

$$= 2\pi (10^{6}) (0.49 \times 10^{-9}) + \pi \frac{20 \times 10^{6}}{20 \times 10^{-6}} (2n-1) (0.49 \times 10^{-9})^{2}$$

$$= 10^{-3} \pi \left[0.98 + (2n-1) (0.24 \ 10^{-3}) \right] \text{ rad}$$

$$= 0.18 \left[0.98 + (2n-1) (0.00024) \right] \text{ deg} \qquad (13)$$

and

$$N_p = \frac{T}{\Delta t} = (2.04 \times 10^9)(20 \times 10^{-6}) = 40,800$$
 samples.

D. Antenna Simulation

The antenna design was the responsibility of JSC. It posed a special problem because a single antenna for the 10 GHz bandwidth (2-12 GHz) would be very difficult to design and build. Secondly, its design largely depended on the JPL radar design, which was not finalized. Table II gives the parameters that were selected for use in the absence of any real antenna characteristics.

E. Terrain Specifications

The terrain to be used initially was to be a model terrain used in previous work, called SINGLESCAT. It contains two discrete scatterers and a single homogeneous field. Table III describes the parameters for this model.

TABLE II

ANTENNA SPECIFICATIONS

*		KANT	Antenna iden+ification, BCD	UNITPAT
*	n _R	SNAC	Boresight nadir at map start, rad	20°,π/9
*	φ _B	SQUINT	Boresight squint at map start, rad	90°,π/2
*	¢	ABW	Anteins szimuth angular coverage, rad	π
×	n _{e1}	EBW	Antenna elevation angular coverage, rad	π
*	C1	PHCPB(3)	Phase center position, body axis xyz, m	0,0,0
<u>.</u>		ABRPY(3)	Antenna attitude, body axis rpy, rad	$0, -\frac{7\pi}{18}, \frac{\pi}{4}$
*		PDRPY(3)	Platform attitude rates, local orbital rpy, rad/sec	0,0,0

TABLE III

TERRAIN SPECIFICATIONS

KSNO	Terrain identification, BCD	SINGLESCAT
NDISC	Number of discretes in terrain model	2
NFLDS	Number of fields in terrain model	1
NSCATS	Total number of scatterers in terrain model	102
EMEAN	Mean echo strength	0.1
DISTAX	x-axis coverage, km	10
DISTY	y-axis coverage, km	10

A meeting was held at NASA/JPL in the third month of the contract, attended by representatives from ARL:UT and Environmental Research Institute of Michigan (ERIM), to evaluate the design objectives and status of the ASAR. The project had schedule and funding difficulties and, subsequently, NASA decided to cancel the entire project. Unfortunately, a substantial portion of the contract resources at ARL:UT had already been expended on the effort, and a simulation had not been run.

The project was reoriented with specific emphasis on three areas: antenna polarization effects, wavelength diversity effects, and implementation of a so-called "burst mode" wavelength diversity concept on a patch-by-patch basis.

III. OTHER SIMULATION INVESTIGATIONS

Figure 1 illustrates the architecture of the OSS simulation. Each intermediate step results in data on tape or disk bulk storage, which permits incremental completion of the entire simulated radar image. For the polarization and wavelength diversity experiments an existing terrain model was utilized, illustrated in Fig. 2. This figure illustrates the scene content of the test terrain as well as images derived from it.

A. Antenna Polarization Effect

A complete simulation would include the polarization sensitivity of individual scatterers and would incorporate the randomly polarized backscattering from the individual scatterers in fields of scatterers, particularly homogeneous fields. The general situation is that the backscattered wave is partially polarized, part of it completely polarized, and part of it unpolarized. Suppose we designate the degree of polarization as the ratio of the polarized power to the total power (following Kraus), or:

$$d = \frac{\text{polarized power}}{\text{total power}} , \qquad (15)$$

and denoting the Stokes parameters as s₀, s₁, s₂, s₃,

$$d = \frac{\sqrt{s_1^2 + s_2^2 + s_3^2}}{s_0} \quad 0 \le d \le 1 \quad . \tag{16}$$



ARL:UT AE-81-130 CRG - GA 9 - 16 - 81





FIGURE 2

IMAGERY FROM ARL: UT SYNTHETIC APERTURE RADAR (SAR) MATH MODEL

3931

These are normalized Stokes parameters, defined as follows, with reference to Fig. 3:

$$Ex = E_{o} \cos \varepsilon \sin \omega t \cos \tau - E_{o} \sin \varepsilon \cos \omega t \sin \tau$$
(17)

$$Ey = E_{o} \cos \varepsilon \sin \omega t \sin \tau + E_{o} \sin \varepsilon \cos \omega t \cos \tau \quad . \tag{18}$$

If we now substitute the time dependent values of Ex and Ey we have

$$E_1 \sin(\omega t - \delta_1) = E_0 (\cos \varepsilon \sin \omega t \cos \tau - \sin \varepsilon \cos \omega t \sin \tau)$$
(19)

$$E_2 \sin(\omega t - \delta_2) = E_0 (\cos \varepsilon \sin \omega t \sin \tau + \sin \varepsilon \cos \omega t \cos \tau)$$
 . (20)

If these are expanded, and sinut terms and cosut terms set equal (which eliminates the time dependence):

$$E_{1} = E_{o} \left(\cos^{2} \varepsilon \, \cos^{2} \tau \, + \, \sin^{2} \varepsilon \, \sin^{2} \tau \right)^{1/2}$$
(21)

$$E_2 = E_0 \left(\cos^2 \varepsilon \, \sin^2 \tau + \sin^2 \varepsilon \, \cos^2 \tau \right)^{1/2} \qquad (22)$$

The flux density in W/m^2 is the Poynting vector \overline{S} :

$$|\overline{S}| = S_x + S_y = \frac{E_1^2 + E_2^2}{Z_o} = \frac{E_o^2}{Z_o}$$
, (23)

where Z_0 is the free space impedance, 377 Ω per square measure, S_x is the Poynting vector for the E_0 wave component polarized to x, and S_y , for the one polarized to y.

$$S_{x} = \frac{E_{1}^{2}}{Z_{o}} = |\overline{S}| (\cos^{2}\varepsilon \ \cos^{2}\tau + \sin^{2}\varepsilon \ \sin^{2}\tau)$$
(24)
$$S_{y} = \frac{E_{2}^{2}}{Z_{o}} = |\overline{S}| (\cos^{2}\varepsilon \ \sin^{2}\tau + \sin^{2}\varepsilon \ \cos^{2}\tau) .$$

The Stokes parameters are now defined as

$$s_{0} = \frac{S}{S} = 1$$

$$s_{1} = \frac{S_{x} - S_{y}}{S} = \frac{\langle E_{1}^{2} \rangle - \langle E_{2}^{2} \rangle}{SZ} = \cos 2\tau , \qquad (25)$$



FIGURE 3 POLARIZATION ELLIPSE

> ARL:UT AE-81-131 CRG - GA 9 - 16 - 81

where <> denotes time averaged value. Then

$$s_{2} = \frac{2}{SZ} \langle E_{1} | E_{2} | \cos \delta \rangle = \langle \cos 2\varepsilon | \sin 2\tau \rangle ,$$

$$s_{3} = \frac{2}{SZ} \langle E_{1} | E_{2} | \cos \delta \rangle = \langle \sin 2\varepsilon \rangle ,$$

$$l \geq s_{1}^{2} + s_{2}^{2} + s_{3}^{2} .$$

These can be written in matrix form

$$S[s_{i}] = S\begin{bmatrix} s_{0} \\ s_{1} \\ s_{2} \\ s_{3} \end{bmatrix}$$

$$i = 0, 1, 2, 3$$

$$= S\begin{bmatrix} 1-d \\ 0 \\ 0 \\ 0 \end{bmatrix} + S\begin{bmatrix} d \\ d \cos 2\varepsilon \cos 2\tau \\ d \cos 2\varepsilon \sin 2\tau \\ d \sin 2\varepsilon \end{bmatrix}$$
(26)
(27)

for a partially polarized wave, where the first term of Eq. (27) is the polarized power density and the second is the unpolarized power density.

The antenna polarization response may also be expressed as a matrix, with A $_{\rm e}$ the effective aperture:

$$A_{e}[a_{1}] = A_{e}\begin{bmatrix}a_{0}\\a_{1}\\a_{2}\\a_{3}\end{bmatrix} m^{2}$$
(28)

Thus the power out of the antenna is given by

$$W = \frac{1}{2} S A_{e}[a_{i}]_{t} [s_{i}]$$

$$= \frac{1}{2} S A_{e} \sum_{i=0}^{3} a_{i} s_{i} W/Hz$$
(29)

The simulation for the APQ-102 uses a linear polarized antenna, with a gain given by

$$G = \frac{4\pi A}{\lambda^2} , \qquad (30)$$

and the magnitude of the gain function can be entered into the simulation via program ANTENA. Substituting the matrix representation for the A $_{\rm e}$ we have

$$G[a_{i}] = \frac{4\pi}{\lambda^{2}} A_{e}[a_{i}] = \frac{4\pi}{\lambda} A_{e}\begin{bmatrix}a_{o}\\a_{1}\\a_{2}\\a_{3}\end{bmatrix}$$
(31)

Combining the polarization matrix for a scatterer, we have

$$G[a_{1},s_{1}] = \frac{4\pi}{\lambda^{2}} \frac{|\sigma|}{2} [a_{0}a_{1}a_{2}a_{3}] \begin{bmatrix} s_{0} \\ s_{1} \\ s_{2} \\ s_{3} \end{bmatrix}$$
(32)

where the substitution of radar cross-section σ is made for the power density S, assuming that the backscattered power density is proportional to the cross section.

To implement this function in program ANTENA requires that the a_1 be specified, as well as the s_1 . The former may reduce to $a_0=1$, $a_1=0$, $a_2=0$, $a_3=0$, or it may depend on platform motion.

The specification of [s] on the other hand would be arbitrary or would depend on measured data for particular types of radar targets or clutter. As a first step, it vas decided to investigate the effects of crosspolarized antennas for transmit and receive, and assume no polarization sensitivity for σ . Although the crosspolarized response of the receive antenna has been measured, it was not available in the azimuth plane, only in elevation. Based on the lobe structure and boresight gain of the elevation pattern, a crosspolarized azimuth response pattern was constructed and used to specify ANTENA. Figure 4 illustrates the pattern used.

The values for the patterns, digitized every 0.33° to a coverage of $\pm 24^\circ$, were entered using an HP9810A with digitizer. The SEASAT radar parameters were used and six scatterers were entered into the terrain model for test purposes. Five of these were given a cross section of 1 m^2 at the center and corners of the 1.4 x 1.4 km mapped area; the other was 26 dB greater at 20 m^2 . The imulation was exercised and the SARCON data were printed out--see the Appendix. Figure 5 shows the displayed results for the co-polarized antenna response. Post-processing was effected at 2 dB/gray shade, with the peak filter magnitude falling in gray shade 16. Figure 5(a) has gray shade 16 turned on and Fig. 5(b)has it off. To expedite processing no range pulse compression was used; hence range sidelobes are not present. Figure 6 is for the same scatterer array but uses a unit antenna pattern, i.e., it is isotropic. There is no appreciable difference since the entire imaged area falls well within the beam of the APO-102 1.3° 3 dB beamwidth for the orbiter altitude of 870 km.

To demonstrate antenna response, a realistic terrain scene without a prohibitively large scattering area was required and it was necessary to place scatterers at ambiguous (with respect to pulse repetition frequency (PRF)) response points. The total azimuth coverage imaged was only 1.4 km; if the terrain model covered only this area, then from an altitude of 870 km along 4.6 km of the orbit (the synthetic array length), only $\pm 0.25^{\circ}$ of the antenna patterns would be used. To create an effective but simple model of terrain, single scatterers were placed at ambiguous points as illustrated in Fig. 7. Only the single scatterer

20





AE-81-132



ORIGINAL PAGE BLACK AND WHITE PHOTOGRAPH



 (a) Six-scatter OSS simulation, all gray shades, brightness on display set for minimum Doppler sidelobes on 100 x scatterer



(b) Gray shade 16 turned off, brightness increased to include all Doppler filter sidelobes

FIGURE 6 OSS SIMULATION OF SIX-SCATTERER ARRAY USING SEASAT SYSTEM WITH UNIT ANTENNA PATTERN IN AZIMUTH, NO PULSE COMPRESSION

AE-81-134







AE-81-135

at the patch center was imaged; however, there were Doppler contributions from all the sidelobe scatterers. Two configurations of scatterers were used; the second one offset the ambiguous point scatterers in graduated sucps 10-30 m from the ambiguity locations.

Figure 8 illustrates the results. Each photograph contains six images of the patch center; each of these is 1.4 x 0.4 km, with 25 m resolution. From the top, the first three strips are of the unoffset terrain model imaged with the isotropic, co-polarized, and crosspolarized patterns. All three patterns were normalized to 1.0 at the peak response. The 1.3t three from the top on the left are images of the offset scatterers for co-polarized, crosspolarized, and isotropic patterns. The top gray shade of the display is set down 20 dB from the peak response of the center pixel to show the weak sidelobe structure.

The right photo has the same order of images, but the top gray shade is 35 dB below the peak response, thus defining more clearly sidelobe response of the system configurations.

Analysis of these results shows a significant reduction in ambiguities between images with the isotropic antenna pattern and the APQ-102 patterns. The co-polarized pattern image shows no ambiguities and has lower sidelobes than the crosspolarized image. The crosspolarized pattern generates an ambiguity due to its high sidelobes. One must be careful in trying to interpret the power level of the ambiguities, because the energy returned outside the main beam is from only a few scatterers and may be lower than the energy returned from an actual continuous terrain area.

B. Frequency Diversity Effects

It was decided to investigate the image variations with wavelength on the scene of Fig. 2, which has been imaged at the SEASAT wavelength of 23.5 cm. Three other wavelength wavelength selected: 1.8, 3.125, and 10.34 cm.

ORIGINAL PAGE BLACK AND WHITE PHOTOGRAPH



(b) Top gray shade of display set 35 dB from the imaged pixel at the patch center



(a) Top gray shade of display set 20 dB down from the imaged pixel at the patch center

FIGURE 8 RESULTS FROM SAR SIMULATION PROGRAM

- 6

To properly implement the simulation the variation of the cross section with wavelength should be included. Other wavelength dependent factors are the antenna response patterns, transmitted power, receiving system noise and, indeed, every factor in the radar range equation either implicitly or directly. In the interest of economy and reduced complexity, however, only the effects on the synthetic array processing were taken into account. The results are not very dramatic, as would be the case if, for example, the cross-section dependency were included. This could involve a simple adjustment since, generally speaking, radar cross section varies proportionally to the square of the wavelength. A useful set of relations might be:

$$\sigma_{L} = 1 m^{2} = 0 dB m^{2}$$

$$\sigma_{S} = \frac{\sigma_{L}(10.34)^{2}}{(23.5)^{2}} = 1.936 \times 10^{-1} \sigma_{L} = -7 dB m^{2}$$

$$\sigma_{X} = \frac{\sigma_{L}(3.125)^{2}}{(23.5)^{2}} = 1.768 \times 10^{-2} \sigma_{L} = -17.5 dB m^{2}$$

$$\sigma_{Ku} = \frac{\sigma_{L}(1.8)^{2}}{(23.5)^{2}} = 5.867 \times 10^{-3} \sigma_{L} = -24 dB m^{2}$$

This is in general true only for perfectly conducting bodies, and is not the general case for clutter targets. For the first simulation effort, only the wavelength parameter was varied, and the resolution cell dimensions were forced to the same values by varying the number of pulses processed or, equivalently, the array length.

Figure 9 presents the four images of the test pattern, photographed with two different exposures. The most obvious effect of the wavelength changes is in the coherent speckle pattern for the homogeneous fields. The data were analyzed statistically, and only very slight changes in the average values were observed. Table IV provides these data for comparison. The simulations were run for the SEASAT radar and the isotropic antenna pattern. The ARL:UT high resolution display system was used to display and photograph the results (Fig. 10).



TABLE IV

PARTIAL RESULTS OF FREQUENCY DIVERSITY STUDY

STATISTICAL DATA

	Wavelength			
Filter Magnitude	23.5 (cm)	10.345 (cm)	3.125 (cm)	1.8 (cm)
Meximum	336.63147	337.97644	334.47785	342.83377
Minimum	6.86×10 ⁻¹²	3.69×10 ⁻¹⁴	5.13×10 ⁻¹³	8.95×10 ⁻¹⁵
Mean	0.18181	0.17562	0.17848	0.180995
Sigma	4.857	4.859	4.849	4.959

SYNTHETIC ARRAY PARAMETERS

Array No. 1	43,262 pts	43,039 pts	42,816 pts	42,816 pts
Array Length, m	4602	2026	612	352.5
Formation Time (sec)	0.617	0.271	0.082	0.047
No. of Pulses	926	916	900	896
PRF, Hz	1,500	3,370	10,970	18,948
Platform Velocity (km/sec)	7.4577	7.4577	7.4577	7.4577

The PRF was increased to obtain approximately the same number of samples (pulses) in array lengths progressively shorter so that resolution would remain the same for the azimuth dimension as wavelength decreased. Had this not been done, the azimuth resolution would have drastically increased as the ratio of array length to wavelength increased.

ORIGINAL PAGE BLACK AND WHITE PHOTOGRAPH





CALIBRATION PATTERN



GRAPHICS



IMAGE CONTOURS FROM SELECTED GREY SHADES

FIGURE 10 ARL:UT HIGH RESOLUTION DISPLAY SYSTEM

IV. TECHNICAL EFFORT SUMMARY

Unfortunately, the dilution of the resources allocated to the simulation efforts by the ASAR project prevented completion of in-depth studies on any of the subjects undertaken. Initial analysis was commenced on a wide swath technique using squinted multiple beams. A major challenge will be the formation of the image from the output of multiple beams tracking the clutter along the velocity vector. Figure 11 illustrates the concept, which will be undertaken in a follow-on effort.

In summary, the ASAR work provided a method for adapting the OSS simulation to an aircraft platform, and to a linear FM (chirped) pulse radar. The analysis indicates the approach to be taken to fully characterize the effects of polarization of the backscattered energy and crosspolarization of the antenna system versus co-polarization of transmit and receive antennas.

Finally, some effects of frequency diversity in the generation of coherent speckle from homogeneous fields were synthesized with the simulation. These efforts point the way to more detailed and fruitful investigations in the future, using the OSS simulation programs.



FIGURE 11 THE GEOMETRY OF THE MULTIPLE BEAM SAR

L-BAND WAVELENGTH DATA

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S-BAND WAVELENGTH DATA

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