THE RADIATION FROM SLOTS IN TRUNCATED DIELECTRIC-COVERED SURFACES

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16. Abstract

A theoretical approach based on the geometrical theory of diffraction is used to study the electromagnetic radiation from a narrow slot in a dielectric-covered perfectly-conducting surface terminated at an edge. The total far-zone field is composed of a geometrical optics field and a diffracted field. The geometrical optics field is the direct radiation from the slot to the field point. The slot also generates surface waves which are incident at the termination of the dielectric cover, where singly-diffracted rays and reflected surface waves are excited. The diffraction and reflection coefficients are obtained from the canonical problem of the diffraction of a surface wave by a right-angle wedge where the dielectric-covered surface is approximated by an impedance surface. This approximation is satisfactory for a very thin cover; however, the radiation from its vertical and faces cannot be neglected in treating the thicker dielectric cover. This is taken into account by using a Kirchhoff-type approximation, which contributes a second term to the diffraction coefficient previously obtained. The contributions from the geometrical optics field, the singly-diffracted rays and all significant multiply-diffracted rays are summed to give the total radiation. Calculated and measured patterns are found to be in good agreement.
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I. INTRODUCTION

The purpose of this study is to examine the effectiveness of the geometrical theory of diffraction (GTD) in calculating the radiation from slots in perfectly-conducting surfaces which are partially covered with dielectric. Configurations of this type are of interest in the design of antenna systems for spacecraft. We consider the radiation from a narrow slot in a dielectric-covered perfectly-conducting surface terminated at an edge as shown in Fig. 1. This is

\[\text{PI: The Field Point in the Illuminated Region}\]
\[\text{PS: The Field Point in the Shadow Region}\]
\[\text{S}_0: \text{Geometrical Optics Ray}\]
\[\text{S}_1: \text{Singly-diffracted Ray}\]
\[\text{S}_2: \text{Doubly-diffracted Ray}\]
\[\text{S}_w: \text{Surface Ray Traveling Parallel to the Dielectric Sheet}\]

Fig. 1
one of the most elementary structures involving dielectric-covered slots; furthermore, measured patterns are available to check the GTD analysis [1].

A theoretical approach to the problem based on the geometrical theory of diffraction [2] is described. The effect of the truncation of the dielectric cover has been ignored in previous analysis, yet this yields the diffracted ray which plays a dominant role in determining the radiation pattern. The total far-zone field is composed of a geometrical optics field and a diffracted field. The geometrical optics field is the direct radiation from the slot to the field point P; it vanishes in the shadow region below the plane containing the surface AB. The slot also excites surface waves which are incident at the termination of the dielectric cover at A and B. The terminations yield singly-diffracted rays and reflected surface waves. For simplicity the thickness $t$ of the dielectric cover is restricted so that only the dominant $TM_0$ surface wave mode is excited. The contributions from the geometrical optics ray, the singly-diffracted rays and all significant multiply-diffracted rays are summed to give the field at P.

The geometrical optics field and the field of the incident surface wave are obtained from the solution to the problem of a narrow slot radiating through a dielectric-covered ground plane of infinite extent. The diffraction coefficient and reflection coefficient for the surface wave incident on the edge A (or B) are determined in the following way. The surface impedance of the grounded, dielectric cover

\begin{equation}
Z_s = Z_0 \frac{k_n}{k_0}
\end{equation}

where $k_0$ and $Z_0$ are the wave number and characteristic impedance of free space, and $k_n$, which is found from the solution of a transcendental equation, is the wave number of the surface wave in the direction normal to the dielectric-covered surface ($k_n$ is imaginary for a lossless dielectric cover). Next, consider a right-angle wedge, one of whose faces is perfectly-conducting, the other with surface impedance $Z_s$. The canonical problem of the diffraction of a surface wave by this right-angle wedge [3] is used to find diffraction and reflection coefficients, which are adequate for sufficiently thin dielectric covers. However, as the thickness of the cover increases, the radiation from the vertical end face AA' (or BB') of the dielectric cover cannot be neglected. This is taken into account using a Kirchhoff-type approximation, where the total electric field within the dielectric cover at its end face radiates in the presence of a right-angle wedge. This contributes a second term to the diffraction coefficient previously obtained.
The calculated and measured patterns compare well, which justifies the use of the geometrical theory of diffraction in this type of problem together with the approximations which have been used to find the diffraction coefficient. The patterns are very sensitive functions of the parameters, such as the thickness of the dielectric cover and the frequency. When the dielectric cover is lossy, the contributions from the diffracted rays decrease as the loss tangent of the dielectric cover increases. This is due to the fact that the surface wave is attenuated as it is incident at the termination of the dielectric cover. The ripples in the patterns in the illuminated region diminish and the level of radiation in the shadow region is reduced.

II. METHOD OF ANALYSIS

According to the geometrical theory of diffraction, the total far-zone field is composed of a geometrical optics field and a diffracted field. In the problem of a narrow slot in a dielectric-covered perfectly-conducting surface terminated at an edge (see Fig. 1), the geometrical optics field is the direct radiation from the slot to the field point; it vanishes in the shadow region. The singly-diffracted field is the field diffracted by the termination of the dielectric cover at A (or B). The termination of the ground plane at C (or D) yields a doubly-diffracted ray. In this chapter, the contribution from each ray will be described in detail.

A. The Geometrical Optics Field and the Field of the Surface Wave

Consider a magnetic line source on an infinite, perfectly-conducting ground plane covered by a dielectric slab of uniform thickness as shown in Fig. 2.

![Diagram of magnetic line source and dielectric slab](image)
This configuration simulates the behavior of a narrow slot radiating through a dielectric cover. It is known that the line source excites a surface wave which propagates along the dielectric slab. It is a straightforward exercise to show that the geometrical optics field \( H_0 \) and the field of the surface wave due to a magnetic line source of unit strength are:

\[
H_0 = -\frac{\omega \epsilon_0 \epsilon_r \cos \theta_0}{\epsilon_r \cos \theta_0 \cos \zeta_0 t + j\sqrt{\epsilon_r \sin^2 \theta_0 \sin \zeta_0 t}} e^{-j(k_0 s_0 - \frac{\pi}{4})} e^{\frac{\omega t}{\sqrt{2} \pi k_0 s_0}}
\]

\[
H_w = -\frac{\omega \epsilon_0 \epsilon_r^2 \lambda^2 \zeta_w}{\beta \sin \zeta_w t \left[ \epsilon_r k_0^2 (\epsilon_r - 1) + \lambda t (\lambda^2 \epsilon_r^2 + \zeta_w^2) \right]} e^{-\lambda x - j\beta y}
\]

where \( \epsilon_r = (\epsilon' - j\epsilon'')/\epsilon_0 \), the relative dielectric constant of the cover, \( k_0 \) is the free space wave number, \( k = k_0 \sqrt{\epsilon_r} \)

\[
\zeta_0 = k_0 \sqrt{\epsilon_r} - \sin^2 \theta_0
\]

\[
\beta = \sqrt{k^2 - \zeta_w^2}
\]

\[
\lambda = \sqrt{\beta^2 - k_0^2}, \quad k_\eta = j\lambda
\]

The value of \( \zeta_w \) is determined from the transcendental equation

\[
\tan \zeta_w t = \epsilon_r \sqrt{\frac{(\epsilon_r - 1) (k_0 t)^2}{(\zeta_w t)^2}} - 1
\]

In the case where the dielectric slab is lossy, \( \epsilon_r \) and \( k \) are complex, and the root of Eq. (6) is complex. A method for calculating the complex root of a transcendental equation is described in Appendix 2. It is seen from Eqs. (4) and (5) that the important parameters of the surface wave \( \beta \) and \( \lambda \) are complex, so that the surface wave attenuates as it propagates.

Throughout this report a time dependence of \( e^{j\omega t} \) is assumed and suppressed.
B. The Field of the Diffracted Rays

As noted in the preceding section, the slot excites a surface wave which propagates along the dielectric cover (slab). This surface wave is diffracted and reflected at the corners A, B shown in Fig. 1, so we seek the diffraction and reflection coefficients from the canonical problem of the surface wave incident on a dielectric-covered perfectly-conducting right-angle bend as shown in Fig. 3a. Since an exact solution to this problem is not available, we will replace it by an approximate canonical problem, which will be solved in two stages.

In the approximate canonical problem, shown in Fig. 3b, the dielectric slab is replaced by the impedance surface described by Eq. (1), with \( k_x \) given by Eq. (5). If this impedance boundary is positioned at the top surface of the cover, the field of the surface wave external to the cover is unaffected; however, it is apparent that the field within the cover is neglected. Thus one would expect the approximation to be good only when the ratio \( K \) of the power in the surface wave field external to the cover to the power within the cover is large. It can be shown that

\[
K = \frac{\varepsilon_r k_x \cos^2 k_x t}{\lambda (k_x t + \frac{1}{2} \sin^2 k_x t)}
\]

It is seen that as \( t \) decreases, the ratio increases; and so the approximate canonical problem of Fig. 3b is useful only for thin dielectric slabs. The behavior of \( K \) as a function of the thickness \( t \) of the slab is shown in Fig. 4, for \( \varepsilon_r = 2.56 \).

Chu et al [3] have solved the problem shown in Fig. 3b; they give expressions for the far-zone diffracted magnetic field and the field of the surface wave reflected at the edge. Their diffracted field is

\[
H_{11} = -H_w \frac{A \cos \frac{\theta}{3}}{\lambda + j k_o \cos \theta \sqrt{\pi k_o}} \frac{2}{j^{1/2}} e^{\frac{5\pi}{12}} e^{-jk_o s_1}
\]

According to the GTD,

\[
H_{11} = H_w D_{11} e^{\frac{-jk_o s_1}{\sqrt{s_1}}}
\]

in which \( H_w \) is the surface wave field at the edge.
Fig. 3a. The surface wave incident on a dielectric-covered perfectly-conducting right-angled bend.

Fig. 3b. Surface impedance model for a dielectric-covered perfectly-conducting right-angled bend.
Fig. 4. The power ratio of the field of surface wave to the field inside the slab.

$\epsilon_r = 2.57$

$t$: THE THICKNESS OF THE DIELECTRIC COVER

$\lambda_0$: THE FREE SPACE WAVELENGTH

$K = \frac{P_{SW}}{P_{SLAB}}$ (dB)

$\frac{t}{\lambda_0}$
and \( D_{11} \) is the diffraction coefficient. From the two preceding equations,

\[
D_{11} = \frac{A \cos \frac{\theta}{3}}{\lambda + jk_0 \cos \theta} \left( 2 \pi \frac{e^{j\frac{5\pi}{12}}}{\pi k_0} \right) ,
\]

where

\[
A = \frac{4j\nu k_0^2 + \lambda^2}{-3j\nu k_0^2 + \lambda^2 I_{1/3} \sqrt{3}(I_{1/3} \lambda - I_{2/3} k_0 e^{-j\frac{2\pi}{3}})}
\]

\[
I_\nu = \frac{2 e^{j\nu \pi}}{k_0 \sin \nu \sin \theta_s}
\]

\[
\theta_s = \frac{\pi}{2} + j \sinh^{-1} \frac{\lambda}{k_0}
\]

The field of the reflected surface wave at the impedance boundary is

\[
H_{1S} = H_w R e^{-j\beta s_0}
\]

where \( \beta \) is given by Eq. (4), \( s_0 \) is the distance along the impedance surface measured from the edge, and the reflection coefficient of the surface wave is

\[
R = \frac{\cos \frac{1}{3}(\theta_s + \pi)}{\cos \frac{1}{3}(\theta_s - \pi)}
\]
In treating the radiation from thicker dielectric covers, where the field within the cover cannot be ignored, it is apparent that the above approximation is inadequate. In particular, we note that there is a significant contribution from the internal field in the form of radiation from the vertical end faces of the slab at A-A' and B-B' in Fig. 1.

This radiation from the vertical end faces of the dielectric cover is taken into account by using a Kirchhoff-type approximation, where the total electric field within the dielectric cover at its end face radiates in the presence of a right-angle wedge. Here again the dielectric cover is approximated by an impedance surface. The equivalent source of this radiation is the magnetic surface current

\[
K_s = \frac{\beta}{\omega \epsilon r} (1 + R) H_w \frac{\cos k_x(x-t)}{\cos k_xt},
\]

where \( k_x = \sqrt{k^2 - \beta^2} \). The magnetic surface current radiates in the presence of the wedge structure shown in Fig. 5. \( R \) is calculated from Eq. (15). To obtain an integral representation for the magnetic field, one seeks the Green's function which satisfies the mixed boundary conditions.

Fig. 5. Line source located at \( x = x', \theta = 0^\circ \) on a right angled wedge with mixed boundary conditions.
This type of the problem can be solved by the introduction of an auxiliary function which is a linear combination of the field and its cartesian derivatives. The auxiliary function is chosen in such a way that it satisfies the wave equation and simple homogeneous boundaries conditions. Once the auxiliary function is obtained, the original field can be determined by solving a partial differential equation. This idea is due to Stoker [4] and Lewy [5] who studied problems in water wave theory. The far-zone Green's function, $G(s_1, \theta; x', 0)$, is derived in Appendix 1, where it is shown that

\begin{equation}
G(s_1, \theta; x', 0) \sim g(\theta; x', 0) \frac{e^{-jk_0s_1}}{\sqrt{s_1}}
\end{equation}

in which $g(\theta; x', 0)$ is a far-field pattern function which is independent of $s_1$.

The diffracted field is then

\begin{equation}
H_{12} = H_{w} D_{12} \frac{e^{-jk_0s_1}}{\sqrt{s_1}}
\end{equation}

where $D_{12}$ is the diffraction coefficient associated with the diffracted field $H_{12}$. From Appendix 1,

\begin{equation}
D_{12}(\theta) = j\beta(1 + R) \int_{0}^{\infty} \frac{\cos kx(x'-t)}{\cos kvt} \cos kx(t) g(\theta; x', 0) dx'.
\end{equation}

This diffracted field contributes a second term to the diffracted field $H_{11}$ previously obtained. Thus the total field diffracted from a wedge with a dielectric cover on one surface can be approximated as

\begin{equation}
H_1(s_1, \theta_1) = H_{11}(s_1, \theta_1) + H_{12}(s_1, \theta_1)
\end{equation}
where it is more appropriate to replace \( \theta \) by \( \theta_1 \) here. With the inclusion of the \( H_{12} \) term, the surface impedance approximation can be used to treat the radiation from dielectric covers of increased thickness, as will be demonstrated in the next section.

The field diffracted from the termination of the dielectric cover is in turn incident on the edge of the ground plane at a distance \( h \) directly below it. This gives rise to

\[
H_2(s_2, \theta_2) = H_w[D_{11}(\theta_1) + D_{12}(\theta_1)] e^{\frac{-jk_0 s_1}{\sqrt{s_1}}} \left( e^{\frac{-jk_0 h}{\sqrt{h}}} \right) \frac{1}{2} D_h(\theta_2, 0) e^{\frac{-jk_0 s_2}{\sqrt{s_2}}},
\]

a doubly-diffracted contribution from the edges C and D in Fig. 1. Here \( D_h(\theta_2, 0) \) is the hard scalar diffraction coefficient given in Reference 6. The factor of \( \frac{1}{2} \) must be introduced at grazing incidence \( (\theta_2' = 0) \) on the edge. This contribution from the lower edges of the ground plane has little effect on the pattern in the illuminated region, which is dominated by the field directly radiated from the slot plus the singly-diffracted contributions from the terminations of the dielectric cover. On the other hand, this contribution appears as a significant ripple in the pattern of the shadow region below the dielectric-covered ground plane. Thus, with reference to Fig. 1, the total field for \( y > 0 \)

\[
H = \begin{cases} 
H_0 + H_{1A} + H_{1B} + H_{2D} & , \quad x > 0 \\
H_{1B} + H_{2C} + H_{2D} & , \quad x < 0
\end{cases}
\]

in which the first subscript 0,1,2 denotes whether the field is incident, singly-diffracted or doubly-diffracted and the second subscript indicates the edge from which the diffracted ray originates. The expression for \( H \) when \( y < 0 \) is similar.

A computer program based on Eq. (23) has been developed; it is described in Appendix 3. In using this program it should be noted that \( \varepsilon_r \) cannot be very close to 1, nor can the thickness of the cover be very close to zero. Thus, the present solution does not reduce to the slot in the ground plane without a dielectric cover. The reason for this limitation is that the distance from the slot required to establish the dominance of the surface wave field increases as \( \varepsilon_r \to 1, \quad t \to 0 \). Under these circumstances the field at the termination of the cover is not simply that of the surface wave; however, this field can
be determined so that the transition to the case of the ground plane without a cover can be made. But this must await further work. The pattern calculation shown in Fig. 7 is based on a separate solution where the surface wave emanating from the slot is replaced by a space wave propagating along the surface of the ground plane, and the diffraction coefficients for the hard boundary are employed at edges A and B.

III. NUMERICAL RESULTS

Eq. (23) is used to calculate the far zone patterns of the configuration shown in Fig. 1. In each case the ground plane length \( L \) is 12.13 inches, the height \( h \) is 1.71 inches and its width (in the direction perpendicular to the page) is 22 inches. A 0.5 inch by 0.062 inch slot is positioned 0.1 inch to the right of the center of the ground plane, thereby introducing a slight asymmetry in the patterns. The axis of the slot is parallel to the edges shown in Fig. 1. The precise dimensions are shown in Fig. 6. The slot is excited at frequencies so that only the TM\(_0\) surface wave mode can exist. The patterns are calculated in the plane of symmetry normal to the axis of the slot for various frequencies and cover thickness.

![Diagram of experimental dielectric-covered ground plane with slot.](image)

\[
\frac{L}{\lambda_0} = 8.24 \quad \text{AT 8.0 GHz}
\]

\[
\frac{L}{\lambda_0} = 10.8 \quad \text{AT 10.5 GHz}
\]

Fig. 6. Experimental dielectric-covered ground plane with slot.

The calculated and measured patterns for a slot in the ground plane without a dielectric cover are shown in Fig. 7. As explained at the end of section II, a separate calculation via the geometrical
Fig. 7. Pattern of a slot in a perfectly-conducting ground plane. Frequency = 8 GHz.
Fig. 8. Pattern of a slot in a dielectric-covered ground plane. Frequency = 8 GHz, \( t = 0.11 \) inch, \( \varepsilon_r = 2.57 \).
Fig. 9. Pattern of a slot in a dielectric-covered ground plane. Frequency = 10.5 GHz. $t = 0.11$ inch, $\varepsilon_r = 2.56$. 

$t = 0.098 \lambda_0$

$t_c = 0.4 \lambda_0$
Fig. 10. Pattern of a slot in a dielectric-covered ground plane. Frequency = 8 GHz. \( t = 0.1875 \) inch, \( \varepsilon_r = 2.56 \).
theory of diffraction is required in this case. Typical calculated and measured* patterns for the dielectric-covered slot are shown in Figs. 8, 9 and 10; in these figures $t_c$ is the thickest dielectric cover in which only the dominant $TM_0$ surface wave mode can propagate. In the illuminated region, the position and level of the lobes of the two patterns are seen to compare in detail, and overall the comparison of the two patterns is good. In Fig. 8, where the dielectric cover is relatively thin, the end face radiation contribution $H_{12}(\theta_1)$ of Eq. (21) is unimportant and could be neglected. However, for the thicker dielectric covers of Figs. 9 and 10, this contribution is significant. The importance of $H_{12}$ is illustrated in Fig. 11, where

*The measured patterns were provided by Mr. W. F. Croswell of the NASA Langley Research Center, Hampton, Va.
patterns calculated with and without this contribution are shown in the illuminated region. It is seen that this contribution is required to bring the calculated pattern into agreement with the measured pattern. In this case the slot is positioned in the center of the ground plane, so the symmetry of the measured pattern with respect to 90° is an indication of its accuracy.

The patterns are very sensitive functions of the parameters, such as the thickness of the dielectric cover and the frequency. This is shown in Fig. 12, where it is seen that a frequency change of less than two percent causes a substantial change in pattern detail. This sensitivity to slight changes in the parameters could in part account for the differences noted between the calculated and measured patterns.

The presence of a dielectric cover on the ground plane substantially increases the pattern level in the shadow region when the dielectric is lossless. As the loss tangent, tan δ, of the dielectric increases, so does the attenuation of the surface wave incident on the termination of the dielectric cover. This in turn weakens the contributions of the singly- and doubly-diffracted fields. As a result, the ripples in the patterns in the illuminated region diminish, and the level of radiation in the shadow region is reduced, as shown in the calculated patterns of Figs. 13 and 14. In Fig. 14, when tan δ = 0.2, the diffracted field components have been so reduced, the pattern is essentially that of the directly-incident (geometrical optics) field.

IV. CONCLUSIONS

The calculated and measured patterns compare well, which justifies the use of the geometrical theory of diffraction in this type of problem together with the approximations which have been used to find the diffraction coefficient. In particular, the method employed to extend the approximation of the impedance boundary in treating edge diffraction appears to be useful. The patterns of the slot in the dielectric covered ground plane are very sensitive functions of the parameters, such as the thickness of the dielectric cover and the frequency. The presence of the cover substantially increases the pattern level in the shadow region when the dielectric is lossless. As the loss tangent increases, the ripples in the patterns in the illuminated region diminish and the level of radiation in the shadow region is reduced.
Fig. 12. Patterns of a slot in a dielectric-covered ground plane: calculated patterns at slightly different frequencies.

\[ t = 0.190 \lambda_0 \text{ at } 12 \text{ GHz} \]
\[ t = 0.1936 \lambda_0 \text{ at } 12.2 \text{ GHz} \]
\[ t_c = 0.4 \lambda_0 \]
Fig. 13. Patterns of a slot in a dielectric-covered ground plane. Frequency = 8 GHz, $t = 0.1875$ inch, $\varepsilon_r = 2.56 \ (1 - j \ tan\delta)$. The values of tan\(\delta\) are shown on the patterns.
Fig. 14. Patterns of a slot in a dielectric-covered ground plane. Frequency = 12 GHz, t = 0.1875 inch, $\varepsilon_r = 2.57 (1-j \tan\delta)$. The values of $\tan\delta$ are shown on the patterns.
REFERENCES


APPENDIX I
THE GREEN'S FUNCTION FOR A RIGHT-ANGLED WEDGE
WITH AN IMPEDANCE BOUNDARY CONDITION

Consider a right-angle wedge $y = 0, x > 0$ and $x = 0, y < D$, and suppose there is a line source located at $(\rho',0)$ as shown in Fig. 5.

The Green's function $G$ satisfies the following differential equation:

\[(A-1) \quad (\nabla^2 + k_0^2) G(x,y;x',y') = -\delta(x-x') \delta(y-y')\]

where

\[
\begin{aligned}
x &= \rho \cos \theta \\
y &= \rho \sin \theta
\end{aligned}
\]

and

\[
\begin{aligned}
x' &= \rho' \cos \theta' = \rho' \\
y' &= \rho' \sin \theta' = 0
\end{aligned}
\]

The boundary conditions of interest here are given by

\[(A-2a) \quad \frac{\partial G}{\partial y} = 0 \quad , \quad y = 0, \quad x > 0
\]

\[(A-2b) \quad \frac{\partial G}{\partial x} - \lambda G = 0 \quad , \quad x = 0, \quad y < 0
\]

Also,

\[(A-2c) \quad G \text{ satisfies the Sommerfeld radiation condition,}
\]

and

\[(A-2d) \quad G \text{ is finite except at } (x',y').
\]

\[\lambda \text{ is equal to } -j k_0 Z_S/Z_0, \text{ where } Z_S \text{ is the surface impedance given by Eq. (1), and in problem of interest here, } Z_S \text{ is such that } \Re \lambda > 0.\]

Our treatment of this problem closely parallels that of Karp [7], except for the manner in which the unknown constant $A$, which will be encountered later, is found.
Let us make a transformation

\[ V(x,y) = (\frac{\partial}{\partial x} - \lambda) G(x,y) \; \]

then \( V \) must satisfy the following differential equation:

\[ (v^2 + k_0^2) V(x,y) = (-\frac{\partial}{\partial x} + \lambda) \delta(x-x') \delta(y-y') \; \]

Using the relationship \( (\partial/\partial x) \delta(x-x') = -(\partial/\partial x') \delta(x-x') \),

\[ (v^2 + k_0^2) V(x,y) = (-\frac{\partial}{\partial x'} + \lambda) \delta(x-x') \delta(y-y') \; \]

The boundary conditions for \( V(x,y) \) are then

\[ \frac{\partial V}{\partial y} = 0 \quad , \quad y = 0, \quad x > 0 \]

\[ V = 0 \quad , \quad x = 0, \quad y < 0 \; \]

The function \( V(x,y) \) need not be finite at the origin since it involves a differentiation of \( G \). The solution to Eq. (A-5) can be obtained by first solving for the Green's function \( G_0(x,y;x',y') \), which satisfies the differential equation

\[ (v^2 + k_0^2) G_0(x,y;x',y') = -\delta(x-x') \delta(y-y') \]

together with the same boundary conditions

\[ \frac{\partial G_0}{\partial y} = 0 \quad , \quad y = 0, \quad x > 0 \]

\[ G_0 = 0 \quad , \quad x = 0, \quad y < 0 \; \]

and the radiation condition.
It can be shown that

\[(A-9) \quad G_0(x,y;x',y') = \frac{2j}{3} \sum_{n=0}^{\infty} \cos \frac{2n+1}{3} \theta \cos \frac{2n+1}{3} \theta' J_{2n+1}^{(2)}(kr') \]

where \(J_y\) is Bessel function of order \(v\) and \(H_v^{(2)}\) is a Hankel function of second kind of order \(v\).

By applying the operator \(-\partial/\partial x' + \lambda\) to \(G_0(x,y;x',y')\), we obtain the following solution for \(V(x,y)\):

\[(A-10) \quad V(x,y;x',y') = -(\partial/\partial x' + \lambda) G_0(x,y;x',y') \]

The complete solution for \(V(x,y)\) is

\[(A-11) \quad V(x,y;x',y') = -(\partial/\partial x' + \lambda) G_0(x,y;x',y') + \sum_{n=0}^{\infty} a_n \cos \frac{2n+1}{3} \theta \cdot \frac{H_{2n+1}^{(2)}(kr')}{3} \]

The last summation contains the class of admissible singular solutions which satisfy the homogeneous equation for \(V\). Since \(V\) cannot be too singular at the edge, the only admissible function of the singular class is the first term; hence,

\[(A-12) \quad a_0 = c_1, \quad a_n = 0, \quad n \geq 1 \]

A particular solution of \((A-3)\) is

\[(A-13) \quad G_0(x,y) = -e^{\lambda x} \int_{x}^{\infty} e^{-\lambda s} V(s,y) \, ds \]

The existence of the integral is guaranteed since \(\text{Re} \lambda \geq 0\).
The function \( G_0(x,y) \) does not satisfy all the conditions of the problem, for it is not a wave function on the negative \( x \)-axis, since its \( y \) derivative is not continuous there. This defect can be remedied by adding a complementary solution for \( G \), obtained from (A-3), to (A-13); thus we obtain

\[
(A-14) \quad G(x,y;x',y') = G_p + \begin{cases} 
  e^{-j\sqrt{k_0^2 + \lambda^2} y} , & y < 0 \\
  0 , & y > 0 
\end{cases}
\]

\( c_1 \) and \( c_2 \) are then determined by imposing the boundary conditions

\[
(A-15a) \quad G(x,0^+) - G(x,0^-) = 0 , \quad x < 0
\]

and

\[
(A-15b) \quad \frac{\partial G(x,0^+)}{\partial y} - \frac{\partial G(x,0^-)}{\partial y} = 0 , \quad x < 0
\]

Numerically it is very difficult to obtain \( c_1 \) and \( c_2 \). This difficulty can be avoided if we choose a suitable function \([7]\), \( H(x,y) \), which has the same singular property as \( H^{(2)}(k_0 \rho) \) and is a homogeneous solution for \( \nabla \).

Let us consider the Green's function \( N \) which satisfies

\[
(A-16) \quad (\nabla^2 + k_0^2) N(x,y;x',y') = -\delta(x-x') \delta(y-y')
\]

with the boundary conditions

\[
(A-17a) \quad \frac{\partial N}{\partial y} = 0 \quad y = 0, \quad x > 0
\]

\[
(A-17b) \quad \frac{\partial N}{\partial x} = 0 \quad x = 0, \quad y < 0
\]

together with the

\[
(A-17c) \quad \text{Radiation Condition.}
\]
It can be shown that

\[
N(x,y;x',y') = - \frac{j}{3} \sum_{n=0}^{\infty} \epsilon_n \cos \frac{2n}{3} \cos \frac{2n}{3} J_{2n}(k_0 r) \frac{H_n^0(k_0)}{2n+1}
\]

where \( \epsilon_n \) is the Neumann's constant

\[
\epsilon_n = \begin{cases} 
1 & n = 0 \\
2 & n = 1, 2, \ldots
\end{cases}
\]

(A-18)

Let \( H = \frac{\partial G}{\partial x'} + \frac{\partial N}{\partial x} \)

(A-19)

\( \therefore (v^2 + k_0^2) H = 0 \).

\( H(x,y) \) is thus a solution of the homogeneous wave equation with the boundary conditions

(A-21a) \( \frac{\partial H}{\partial y} = 0 \) \( y = 0, \ x > 0 \)

(A-21b) \( H = 0 \) \( x = 0, \ y < 0 \)

together with

(A-21c) the Radiation Condition.

Note that the leading term of \( \partial N/\partial x \) has the same singular property as \( \frac{H_n^0(k_0)}{2n+1} \).

The complete solution for \( V \) is then

(A-22) \( V(x,y;x',y') = - (\frac{3}{\partial x'} + \lambda) G_0(x,y;x',y') + A \ H(x,y;x',y') \)

where \( A \) is a constant to be determined.
That $G$ satisfies the wave equation can be shown from the fact that
\[
G_x = \nabla + \lambda G \\
G_{xx} = \nabla + \lambda \nabla + \lambda^2 G
\]
also
\[
\nabla_{yy} = -\kappa_0^2 \nabla + \left( \frac{\partial}{\partial x'} + \lambda \right) \delta(s-x') \delta(y-y')
\]
\[
\Rightarrow G_{xx} + G_{yy} + \kappa_0^2 G = \nabla_x + \lambda \nabla + \lambda^2 G - e^{\frac{\lambda x}{x}} \int_{x}^{\infty} e^{-\kappa_0 \delta(s,y)d\delta} + \kappa_0^2 G.
\]

Integrating by parts twice in the above integral,
\[
G_{xx} + G_{yy} + \kappa_0^2 G = -(\frac{\partial}{\partial x'} + \lambda) e^{\frac{\lambda x}{x}} \delta(y-y') \int_{x}^{\infty} \delta(s-x') \delta y ds
\]
\[
= -(\frac{\partial}{\partial x'} + \lambda) e^{\frac{\lambda x}{x}} u(x-x') \delta(y-y')
\]
\[
= -e^{\frac{\lambda(x-x')}{x}} \frac{\partial}{\partial x} u(x-x') \delta(y-y')
\]
\[
= \delta(x-x') \delta(y-y')
\]

where $u(x-x')$ is a unit step function.

In the far zone, we observe that $G_0, N, G$ and $\nabla$ have the asymptotic form

(A-23a) $G_0 \approx \frac{e^{-jk_0\rho}}{\sqrt{\rho}} g_0(\theta;x',y')$

(A-23b) $N \approx \frac{e^{-jk_0\rho}}{\sqrt{\rho}} n(\theta;x',y')$

(A-23c) $G \approx \frac{e^{-jk_0\rho}}{\sqrt{\rho}} g(\theta;x',y')$

and
\[ V \approx \frac{e^{-jk_0 \rho}}{\sqrt{\rho}} u(\theta; x', y') \]

Since the far-zone field is of interest, only those terms which are of \( O(1/\sqrt{\rho}) \) are retained, the operator \( \partial/\partial x \) can be approximated by \(-jk \cos \theta\); thus we obtain

\[ G(x, y; x', y') \approx \frac{[\lambda \frac{\partial}{\partial x} - \lambda] G_0 + jk_0 \cos \theta A N}{jk_0 \cos \theta - \lambda} \]

Hwang [*] determines the constant \( A \) by transforming the function \( G_0 \) and \( N \) into the integral representations which are then evaluated asymptotically by the modified Pauli-Clemmow method of steepest descent. From the asymptotic solution, we can identify the ray-optical behavior of the field. The pole contributions give rise to the geometrical optics field which is the sum of the incident field and the reflected field. From this we obtain

\[ A = 1 \]

Thus,

\[ G(x, y; x', y') \approx \frac{jk_0 \cos \theta N - \lambda G_0}{jk_0 \cos \theta - \lambda} \]

in the far zone, where \( N \) and \( G_0 \) are given by Eqs. (23a) and (23b).

---

APPENDIX II
ON CALCULATING THE COMPLEX ROOT OF A TRANSCENDENTAL EQUATION

The problem of finding the complex roots of a transcendental equation is usually reduced to the problem of finding the roots of two simultaneous nonlinear equations. The two nonlinear equations occur because the real and imaginary part of a complex function must also equal zero when the complex function \( f(z) = 0 \). The method of finding the roots of simultaneous, nonlinear equations has been discussed in many books; but sometimes it is tedious to reduce a complex function to two real nonlinear functions. In this appendix we point out that Newton's method for the real roots of a real function can be extended to find the complex roots of a complex function.

Suppose that we seek a solution \( z_0 \) of a function \( f(z, \epsilon) \) such that

\[
(A-27) \quad f(z_0, \epsilon) = 0 ,
\]

where \( \epsilon \) is a complex parameter.

Using Taylor's expansion,

\[
(A-28) \quad f(z_0, \epsilon) = f(z_{01}, \epsilon) + f'(z_{01}, \epsilon) \Delta z_1 + \epsilon \]

where \( z_{01} \) is an initial estimate of the root, which is assumed to be close to \( z_0 \). For example, \( z_{01} \) could be found by solving a related problem exactly.

Let

\[
(A-29) \quad \Delta z_1 = z_0 - z_{01} .
\]

From Eqs. (A-27) and (A-28),

\[
(A-30) \quad \Delta z_{12} = - \frac{f(z_{01}, \epsilon)}{f'(z_{01}, \epsilon)} \approx \Delta z_1 .
\]

Next, replace \( z_0 \) by \( z_{02} = z_{01} + \Delta z_{12} \), and repeat the procedure; in this way we can generate successive approximation, and after \( N \) iterations,
(A-31) \[ Z_0 = Z_{01} + \sum_{i=1}^{N} \Delta Z_{ia} \] 

where

(\text{A-32}) \[ \Delta Z_{ia} = -\frac{f(Z_{0i}, \varepsilon)}{f'(Z_{0i}, \varepsilon)} \] 

When \( Z_{01} \) is chosen sufficiently close to the root \( Z_0 \) and \( f'(Z_{0i}, \varepsilon) \neq 0 \), the process will converge, i.e., \( |\Delta Z_{i+1a}| < |\Delta Z_{ia}| \). The iterative procedure can then be terminated when \( |\Delta Z_{ia}| < \delta \), where \( \delta \) is a specified small number.
APPENDIX III
THE FORTRAN IV PROGRAM FOR CALCULATING
THE FAR-ZONE RADIATION PATTERN.

C PATTERN CALCULATION OF SLAB RADIATOR IN A DIELECTRIC-COATED METAL PLATE
C THIS PROGRAM IS GLOBALLY FOR 0 < D < 0.5XLAMBD
C LAMBD = FREE SPACE WAVE LENGTHS
C THIS PROGRAM CANNOT BE USED WHEN ESL=1.0 AND/OR 0=0.0
C
C FSR = RELATIVE DIELECTRIC CONSTANT
C ES0 = FREE SPACE DIELECTRIC CONSTANT
C EL = DIELECTRIC CONSTANT OF LOSSY SLAB
C D = THICKNESS OF DIELECTRIC COATING IN INCHES
C F = FREQUENCY IN CPS
C R = FREE-SPACE WAVE NUMBER
C RK = DIELECTRIC WAVE NUMBER FOR LOSSLESS SLAB
C VI = THICKNESS OF THIN-CATED GROUND PLANE IN INCHES (NOT INCLUDING
C THE THICKNESS OF SLAB)
C W1 = WIDTH OF DIELECTRIC COATING FORM THE SOURCE TO THE RIGHT
C CORNER IN INCHES
C XL = TOTAL THICKNESS OF DIELECTRIC COATING IN INCHES
C XLT = LOSS TANGENT OF LOSSY SLAB
C T = CONVERSION FACTOR (1 INCH = 0.0254METERS)
C CI = SURFACE-WAVE ATTENUATION CONSTANT
C AUTO = SURFACE-WAVE PROPAGATION CONSTANT
C HQ = DIRECT RADIATION FIELD
C HQ1 = DIFFRACTION FIELD (RIGHT SIDE)
C HQ2 = DIFFRACTION FIELD (LEFT SIDE)
C HY = SLAB RADIATION FIELD
C HT = TOTAL RADIATION FIELD
C FN = NORMALIZED CONSTANT OF THE TOTAL RADIATION FIELD IN OR AT
C 90-DEGREES
C HRT = TOTAL RADIATION FIELD INCLUDING SLAB RADIATION
C DHRT = TOTAL RADIATION FIELD IN DATA SLAB RADIATION)
C PHD = ASPECT ANGLE IN DEGREES
C
C COMMON RJ(150),RY(150)
DIMENSION AMH(180),AHM(180)
COMPLEX HGO, THET, V1, R2, A1, A2, A3, HT, CCS1, HR, HL, HD1, HD2, HY
COMPLEX HIH
COMPLEX CN, CO, C2, HTT
COMPLEX HYF, HYR, CF, GR
COMPLEX CCS1, CCS2
COMPLEX MD10, MD20, HR1, HR11, HL1, HL11
COMPLEX HP, HR
COMPLEX HM1, HM2, HM4, HM5, M
COMPLEX MD10, MD11, MD20, MD21, DO, DVDR, DVOL
COMPLEX CSS1, CSS2, C1, C2
COMPLEX EL, Z1, Z2, CH, CRETA, CESIL, CESR, TS, C1
PI=3.141592
1212 READ (5,1111) FND=1,112) ESL, F, F, D, XL, W1, VI, XL, Y
1111 FORMAT (F4.2, F10.3, F6.2, F4.7, F4.9, 2)
2 H=XL-W1
WRITE (6,1313) F, D, H, W
1313 FORMAT (1H1, ' FREQUENCY= ', E10.3, 'Hz SLAB THICKNESS=', 'FR.4', ' Inch
2 1 H1=' F, F, 5, '21 F, F, 4)
WRITE (6,1444) HI, W
1444 FORMAT (' PHD = ASPECT ANGLE IN DEGREES', ' DHRT = TOTAL RADIATION
IN FIELD IN DB', ' /
2 R=2.0*PI*F/3.0*EN
F=0 = 8.49E-12
T = 2.54F-12
H1=10T
H2=2ST

32
CALL SV'P(F,FSR,SR,n,y,FSIL,*TA,U,FSR)

X=FSIL(4)

AA=FSR+y

P=XTA*AA

CALL HS(P,F,EL,XI,7,IE)

Z=(2.,0PI/6,.,0)*4.,0PI/3,0.-7,0EL

C=TA(2.702/(1.0))

C=FSORT(Z-k-202/(1.0))

CIL=Z/n

CFSR=EL/FSR

CETA=CMPLX(CETA)

C=CMPLX(CESIL)

CFSR=CMPLX(CFSR)

CALL HTSE,H,R,TS,IE

C C2 IS THE REFLECTION COEFFICIENT

C2=-CCOS((TS+PI)/3.)/CCOS((TS-PI)/3.)

I=0

PHD =-1.0

PHD = PHD + 2.0

PH = PHI+n,0,0,745

J=0

X=CCSORT(CESR-COS(PH)*COS(PH))

H=2.,0PI/6,0*COS(CESR)

C=CMPLX(CESR)

C=CMPLX(CESR)

H=2.,0PI/6,0*COS(CESR)

C=CMPLX(CESR)

C=CMPLX(CESR)

A=CMPLX(0.,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,0,
CALL PFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,@, @)

CALL PFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,@, @)

CALL PFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,@, @)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

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CALL PHFRG(FW, L, X, Y, PH, XL, A)

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CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

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CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)

CALL PHFRG(FW, L, X, Y, PH, XL, A)

CALL RHFJ(G,R, E)
TSI = TSI
NEL = FEL + 1.5

10 CALL CTS(CU, A, TSI, TS, IER)

RETURN
END

SUBROUTINE CTS(CU, A, TSI, TS, IER)

COMPLEX F, CU, TS, OTS, TSI, TS, IC, TSI

F(CU, A, TC) = (CSORT(1.2 + CU * (1.0 - A)) - CSIN(TC)) / CCMS(TC)

N = 0

OTS = F(CU, A, TSI)
T1 = CARS(OTS)

TS1 = TSO + OTS

A = CARS(CSORT(1.2 + CU * (1.0 - A)) - CSIN(TSI))

TS1 = F(CU, A, TSI)
T2 = CARS(TS1)

IF (A < 1.0 - 5) GO TO 2
IF (T2 < GT, T1) GO TO 3

T1 = T2

TS1 = TSI1 + OTS

N = N + 1

GO TO 1

IER = 1

WRITE (6, 4)

FORMAT('THIS ITERATION DOES NOT CONVERGE')

GO TO 7

IER = 1

WRITE (6, 10)

FORMAT('THIS COMPUTATION DOES NOT CONVERGE IN 20 ITERATIONS')

RETURN
END

SUBROUTINE HSMP(D, F, EL, X, Z, IER)

COMPLEX EL, Z, RZ, ZI, ZU, EP

ZI = CMPLX(1.0, 0.0)

PEL = L.E-5

E = ABS(PEL)

RE = REAL(EL)

A = RAS(E/RE)

ZI = ZU

IF (A < I.4) GO TO 10

F = CMPLX(RE, -RE*EL)

CALL CRSHP(R, F, EL, ZI, RZ, IER)

IF (IER < E/10) GO TO 3

F = CMPLX(RE, -RE*EL)

CALL CRSHP(R, F, EL, ZI, RZ, IER)

RETURN
END
\[ n = 2 \cdot \pi H / 3 \cdot \text{E08} \]

\[ ZK = ((2 \cdot \pi H)^{M2})^{E+} \cdot \pi E-7 \cdot \text{E1} \]

\[ N = 0 \]

\[ DZ = -((F(Z1) - G(EL, ES0, ZK, H, D, Z0)) / (F(P(ZU) - G(EL, ES0, ZK, H, D, Z0)))) \]

\[ T1 = \text{CAR} \cdot (n2) \]

\[ Z1 = (T+2O) \]

\[ DZ1 = -((F(Z1) - G(EL, ES0, ZK, H, D, Z1)) / (F(P(Z1) - G(EL, ES0, ZK, H, D, Z1)))) \]

\[ T2 = \text{CAR} \cdot S(DZ1) \]

\[ IF(A, LT, 1, E-5) \text{GO TO 2} \]

\[ IF(T2, GT, T1) \text{GO TO 3} \]

\[ T1 = T2 \]

\[ Z1 = Z1 + DZ1 \]

\[ N = N + 1 \]

\[ IF(N, GE, 30) \text{GO TO 5} \]

\[ GO TO 1 \]

\[ IF(RN = 0) \]

\[ RZ = ZI \]

\[ GO TO 7 \]

\[ 1) \]

\[ IER = 1 \]

\[ WRITE(6, !) \]

\[ IF(A, LT, 1, E-5) \text{GO TO 1000} \]

\[ N = 0 \]

\[ IF(SV, GE, TV) \text{GO TO 1111} \]

\[ X2 = ZR \]

\[ GO TO 992 \]

\[ 1111 X2 = TV - 0.0001 \]

\[ 992 Y2 = F(X2) \]

\[ 1 \]

\[ X = (X1 + X2) / 2.0 \]

\[ N = N + 1 \]

\[ IF(X, GT, 30) \text{GO TO 2} \]

\[ IF(F(A, LT, 1, E-5) \text{GO TO 101} \]

\[ X2 = X \]

\[ IF((X2 - X1), LT, 1, GE, 5) \text{GO TO 101} \]

\[ GO TO 1 \]

\[ 101 X1 = X \]

\[ IF((X2 - X1), LT, 1, GE, 5) \text{GO TO 101} \]

\[ 101 \text{E1} = Z/0 \]

\[ \text{META} = \text{SORT(AR*2 - ESIL*2)} \]

\[ (n = \text{SORT(AR*2 - ESIL*2)} \]

\[ 36 \]
SUBROUTINE THFT(P,C)

THIS ROUTINE IS TO COMPUTE A CONSTANT BY FINDING A ROOT OF A
POLYNOMIAL BY USING THE SECANT METHOD IN ORDER TO COMPUTE THE
CHU-KIYUHUTAN'S COEFFICIENT

F(X) = SINH(X)-P
X = 0.0
X1 = P
Y = F(X)
Y1 = F(X1)
GO TO 2,20
X2 = (X*F(X1)-X1*F(X))/(F(X1)-F(X))
Y = F(X2)
IF(ABS(X2-X1)*LT.1.E-5) GO TO 2
X = X1
1
X1 = X2
WRITE(6,6)
FORMAT(/36HOF AILED TO CONVERGE IN
GO TO 3
C = X2
RETURN
END

SUBROUTINE DFRCF(D,XN,Y,R,LMDA)

THIS ROUTINE IS TO COMPUTE THE DIFFRACTION COEFFICIENT
COMPLEX F1,F2,J,N1,N2,D,F1,F2,S
PI=3.1415927
RR=1.0745329
ARG1=(PI+RR)/(2.0*XN)
ARG2=(PI-RR)/(2.0*XN)
CX1=COS(ARG1)
CX2=COS(ARG2)
SX1=SIN(ARG1)
SX2=SIN(ARG2)
X1=(HR+PI)/(2.0*XN*PI)
N1=X1
E1=X1-N1
IF(E1.GT.0.5) N1=M1+1
IF(E1.LT.-0.5) N1=N1-1
FN1=FLOAT(N1)
X2=(HR-PI)/(2.0*XN*PI)
N2=X2
E2=X2-N2
IF(E2.GT.0.5) N2=M2+1
IF(E2.LT.-0.5) N2=N2-1
FN2=FLOAT(N2)
A1=1.0+COS(-HR+2.0*XN*PI*FN1)
A2=1.0+COS(-HR+2.0*XN*PI*FN2)
SA1=SORT(A1)
SA2=SORT(A2)
XX=(SORT(2.0*PI*XY))*SA1
YY=(SORT(2.0*PI*XY))*SA2
CALL CS(C1, S1, XXS)
CC1 = 0.5 - C1
SS1 = 0.5 - S1
F1J = P0 * CMPLX(SS1, CC1)
CALL CS(C2, S2, YYS)
CC2 = 0.5 - C2
SS2 = 0.5 - S2
F2J = P0 * CMPLX(SS2, CC2)
P0 = P1/4, n

C = EXP(0)
R = EXP(0)

S = (-0.25) * EXP(XXS)
T1 = S * 2.0 * CMPLX(0.0, XXS)
T2 = S * 2.0 * CMPLX(0.0, YYS)

RETURN
END

SUBROUTINE HSLAR (VI, F, CESR, CU, CHETA, CESIL, CCS, PHO, HT)
THIS SUBRUTINE IS TO COMPUTE THE SLAB RADIATION FIELD

COMPLEX CCS, HY, HT, CESR, CU, CHETA, CESIL, XXS, XKK
PI = 3.14159
ESU = H.R5E-12
XLMNA = 3.0F.01/F

XXS = CSORT(ZK-CRETA=CRETA)
XKK = XXS

HT = CMPLX(0.0, 0.0, 0.0, 0.0)

IF(DI = 0, 0.05*XLMNA)

CALL CASER(D, F, H, V1, CESR, CU, CHETA, CESIL, XLMNA, 0.0, 0.0, 0.0, 0.0)

RETURN
END

SUBROUTINE CASER (DI, F, H, V1, CESR, CU, CHETA, CESIL, XLMNA, 0.0, 0.0, 0.0, 0.0)

PH = P4 * 0.01745
IF(PHGT 270.0) = PH - 270.0)

RETURN
END

SUBROUTINE GREENF (PH, ARG, UK, XLMNA, F, G)

ARG = RK * UK

HY = F

RETURN
END

RETURN
END

RETURN
END

RETURN
END

RETURN
END
CALL PFRCF(HHY, X, Y, Z, C, XLMDA)
Y2=(I+IV1)/XLMNT
CALL HFLRCF(Y, X, Z, C, XLMDA)
WM2=CMHYXHYXH2CMXX(CPLX(0,1)-MKHY(YV1)-HXYV1)/SQR(YV1)
IF (PHI .LT. 0.) GOTO 1112
IF (PHI .LT. 180.) GOTO 1111
H=HY+HY2
GOTO 2
1112 H=0
GOTO 2
1111 H=HY+HY1+HY2
2 CONTINUE
RETURN
END
SUBROUTINE GREENF(PHI, ARG, UK, XLMDA, F)
COMPLEX F, N, M, NH, R, X, P, UK, AI
P(X) = CECP(CPLX(0, X))
PI = 3.141592
PH = PHI .LT. PI / 180.
R = 2.*PI / XLMDA
XM = 1.5
AI = CPLX(0, 1.)
N = (0, 0)
DO 5 M = 1, 20
I = M-1
FM = 0.
IF (I .LT. 0) FM = 1.
NM = EMRNP(1 * PI / (2. * XM)) * COS(1 * PHI / XM)
N = N + NM
AM = CAHS(NM)
IF (ANH .LT. 1.E-30) GOTO 44
CONTINUE
44 G = (0., 0.)
DO 15 M = 1, 20
I = M-1
NM = EMRNP((2. * I + 1) / (4. * XM)) * COS((2. * I + 1.) * PHI / (2. * XM))
G = G + GM
AGM = CAHS(GM)
IF (AGM .LT. 1.E-30) GOTO 55
CONTINUE
55 C = SORT(2., (PM/P)) / XM
G = GCOP(-PI/4.)
NM = GCOP(-PI/4.) / 2.
RU = REAL(UK)
AI = AIMAG(UK)
IF (PHI .LT. 90.) OR (PHI .LT. 270.) GOTO 11
IF (RI .LT. 0.) AND (AI .LT. 0.) GOTO 22
F = (AI * COS(PHI) + UK * G) / (AI * COS(PHI) * UK)
GOTO 33
11 F = G
GOTO 33
22 F = N
33 RETURN
END
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