Microstrip Reflectarray Antenna for the SCANSCAT Radar Application

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ABSTRACT

This publication presents an antenna system that has been proposed as one of the candidates for the SCANSCAT (Scanned Scatterometer) radar application. It is the mechanically steered planar microstrip reflectarray. Due to its thin, lightweight structure, the antenna’s mechanical rotation will impose minimum angular momentum for the spacecraft. Since no power-dividing circuitry is needed for its many radiating microstrip patches, this electrically large array antenna demonstrates excellent power efficiency. In addition, this fairly new antenna concept can provide many significant advantages over a conventional parabolic reflector.

The basic formulation for the radiation fields of the microstrip reflectarray is presented. This formulation is based on the array theory augmented by the Uniform Geometrical Theory of Diffraction (UTD). A computer code for analyzing the microstrip reflectarray’s performances, such as far-field patterns, efficiency, etc., is also listed in this report. It is proposed here that a breadboard unit of this microstrip reflectarray should be constructed and tested in the future to validate the calculated performance. The antenna concept presented here can also be applied in many other types of radars where a large array antenna is needed.
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I. Executive Summary

The mechanically steered flat microstrip reflectarray antenna has been proposed as one of the candidate antennas for the SCANSCAT (Scanned Scatterometer) radar application. Due to its thin, lightweight structure, the antenna's mechanical rotation will impose minimum angular momentum for the spacecraft. Since no power dividing circuitry is needed for its many radiating microstrip patches, this electrically large array antenna demonstrates excellent power efficiency. As will be described in this report, this fairly new antenna concept can provide many significant advantages over a conventional parabolic reflector.

The tasks that have been completed this year are the basic formulation of the antenna radiation fields and the generation of a computer code for analyzing the microstrip reflectarray's performances, such as far-field patterns, efficiency, etc. The formulation is based on the array theory augmented by the Uniform Geometrical Theory of Diffraction (UTD). It is proposed here that a breadboard unit of this microstrip reflectarray should be constructed and tested in the future to validate the calculated performance. This antenna concept can also be applied in many other types of radars where a large array antenna is needed.

II. Introduction

1. Antenna Requirements:

The Ku-band SCANSCAT antenna is required to generate two sets of pencil beams, as shown in Figure 1, to map the surface of the Earth for scatterometer application. One set should radiate at 36° from the nadir direction, while the other should be pointed at 49° from the nadir. Both sets of beams should be able to transmit and receive horizontally polarized electrical fields. Due to the azimuth scan speed of 16.4 rpm for the mechanical platform and relatively slower radar pulse return time, the transmit and receive
beams at 36° elevation need to be separated in azimuth by 0.59°. Similarly, the transmit and receive beams at 49° elevation should be separated by 0.77° in azimuth. Consequently, a total of four beams are to be generated at the frequency of 13.995 GHz. Each beam needs to have a 3-dB beamwidth of not more than 0.7° with a peak gain of 47 dBi or more and sidelobe level not higher than -20dB.

2. Previously Proposed Concepts:

A previously proposed antenna system was a mechanically steered dual-reflector configuration as illustrated in Figure 2. This configuration, although simple in design and relatively low in cost, will require large physical volume, mass, and, worst of all, a momentum compensation system that will result in even larger mass. As a consequence, a task was recently engaged to study other antenna concepts that will lead to smaller antenna volume, mass, and spin momentum. Quite a few concepts have been investigated, which include electronically scanned phased arrays, hybrid electronically/mechanically scanned arrays, and mechanically steered arrays. The phased array approach was ruled out due to its extremely high cost and complexity. The only technically viable phased array approach is the active array with distributed T/R modules. With approximately 33,000 radiating elements, T/R modules, and phase shifters required, the whole antenna system will cost about $20 million. In addition to the high cost, it will be difficult (if not impossible) for the phased array to generate horizontally polarized beams in all the azimuth directions required. Also, an impractically large amount of D.C. power (in the order of many Kilowatts) may be needed to bias and control the large number of T/R modules and phase shifters.

After a trade-off study, one antenna concept was selected for further investigation. This is the mechanically steered microstrip reflectarray, which consists of a single flat array disc (3.1-meter diameter) that is space-fed by a small low-gain antenna and
mechanically spun in azimuth. This microstrip reflectarray offers much lower spin momentum, physical volume, and mass than the dual-reflector system. A detailed description of this antenna concept, as well as its advantages, are given in the following sections. Theoretical analysis of the antenna’s performance was also carried out in this study effort. The basic array theory augmented by the Uniform Geometrical Theory of Diffraction was utilized for the theoretical analysis. A user oriented computer code for analyzing the microstrip reflectarray has been successfully used to produce many valuable data.

III. Description of the Microstrip Reflectarray

When many antenna elements with open or short circuited terminations are arranged in a planar aperture and are illuminated by a feed antenna as shown in Figure 3, these elements will re-radiate their illuminated energy into space. The total re-radiated energy will be non-coherent in phase, even when all the elements and their terminations are identical. This is because the fields that propagate to the elements from the feed have different path lengths, $S_1, S_2, ..., S_N$, as shown in Figure 3(b), and thus form different phases. However, if each element’s phase is adjusted to compensate for these different path lengths, the total re-radiated field can be made coherent and concentrated toward a specific direction. Many different types of radiators, such as horn, dipole, etc., can be used on the planar structure. If this planar structure is required to be thin, then a printed-circuit type of element needs to be employed. Several of these printed-circuit flat plate antennas have been attempted previously without much success. An early attempt used the flat plate concept as a lens rather than as a reflector. Very low efficiency (25%) was reported. Recently, Malibu Research Center has demonstrated a flat plate reflector without showing much data on efficiency. Both above attempts used either resonant slots or dipoles without any phase delaying transmission lines. Only the size of the slot or dipole is varied for phase trimming which is achieved by adding
reactance into the element's radiation impedance. This is equivalent to saying that the phase of the dipole's surface current is different for different dipole lengths. With properly designed phase distribution, beam coherence can be achieved by these arrays. This, however, will result in reduced radiation efficiency. Since, for a particular frequency, there is only one optimum size of the resonant structure to transmit through or reflect energy, other sizes will result in low amplitude. Reference [4] printed that, "amplitude must be sacrificed at the expense of phase change". A more recent study[6] has used equal-size dipoles with periodic spacing so that all the dipoles have the same illumination phase as the feed. This is the so-called frequency grating and is very sensitive to frequency change. It is therefore used as a frequency scanned offset-fed flat reflector antenna. Aperture efficiency of 50% has been achieved by this antenna. Due to its required offset-fed configuration, this antenna cannot be effectively used in the SCANSCAT application.

The flat plate antenna proposed here uses the reflectarray[7] concept where a short transmission line is attached to each radiator for phase adjustment. The electrical lengths of these transmission lines are made different depending on their radiators' positions from the feed. All the radiators, however, are identical in size and are made of thin microstrip patches. This antenna, as shown in Figure 4, is called the microstrip reflectarray. It is composed of a thin (≤0.02 wavelength) slab of dielectric material having one side completely covered with a layer of thin metal (which serves as a ground plane) and the other side etched with many identical metallic microstrip patches. A feed antenna, located at an optimally designed distance from the flat plate, will effectively illuminate all the metallic patches. The size of each patch, which can be rectangular, square, or circular, is made to resonate at the same frequency as the feed antenna. A short transmission line is connected to each patch at one end with the other end of the line either open or short circuited. This transmission line can be either a microstrip line etched on the
same side of the patches or a stripline sandwiched in an additional layered structure behind the ground plane. The advantage of the microstrip line is ease of fabrication with very little impact on antenna weight, while that of the stripline is minimum interference to the patch’s radiation. When the radiation field of the feed antenna (in transmit mode) strikes each patch, the received resonant field of the patch will travel through its connected transmission line and be reflected by its open or short circuited termination and then re-radiate through the patch into space. Thus, all the microstrip patches behave as re-radiators, while the short transmission lines serve as phase delay lines. The lengths of these transmission lines are intentionally made different for differently located patches so that the path delay differences from the feed antenna can be compensated. With proper design and calibration of these line lengths, the re-radiated fields from all the patches can be made coherent and concentrated toward the broadside direction. Also by re-designing the line lengths, the main beam can be directed toward other directions. Since the required phase changes for all the elements are between $0^\circ$ and $360^\circ$, the maximum length needed for the transmission line is only a half-wavelength. Consequently, the insertion loss associated with these short lines will be insignificantly small. However, this half-wavelength transmission line will work for a narrow bandwidth ($\leq 1\%$) application. For a wider bandwidth, a frequency excursion error will occur, especially for the outer elements of the array (assuming the feed is located at the center axis of the array). In other words, the phase will accumulate more error for the outer elements. This accumulated phase error can be reduced by using longer transmission lines for the center elements and/or by using a larger $f/D$ ratio (where $f$ is the distance between the feed and the patches, and $D$ is the diameter of the reflectarray).

Since the microstrip reflectarray does not require any power divider, its efficiency in a large array system is much higher than a conventional array having the same aperture size. One possible drawback of this reflectarray is that, in addition to the re-
radiated fields from the patches, there will also be scattered field from the patches, reflected field from the ground plane (especially at off-resonant frequencies of the patch), and diffracted fields from edges of the flat plate. These backscattered fields may increase the sidelobe level and possibly distort the main beam shape. However, as long as the aperture directivity of the flat plate is sufficiently higher (25dB or more) than the feed directivity, the backscattered energy will be insignificantly small. In other words, as will be demonstrated in a later section, the microstrip reflectarray will be an efficient antenna system only if it has a large number of elements (thousands or more).

IV. Application to SCANSCAT

The proposed microstrip reflectarray for SCANSCAT is configured in Figure 5 where each patch has two orthogonally connected transmission lines with different lengths. Each one corresponds to a different elevation beam. Although not required, this orthogonal connection and the proper phase settings can separate the two different elevation beams 90° apart in azimuth. To meet the four-beam requirement of SCANSCAT, four feeds are needed as shown in Figure 5. Each two with the same polarization, due to their spatial separation, will generate the two separated transmit and receive beams. This is because each different feed location will form a different set of phases to illuminate the patches and, thus, generate a different beam position. Each two feeds that have different polarizations will generate two beams at different elevation and azimuth angles due to the two different settings of transmission line lengths on the microstrip patches. Because of the elegance of this design, all four beams will have horizontal polarization as required. These four beams are to be scanned in azimuth by spinning mechanically at the center of the circular flat plate. Due to the fact that the mass of the circular flat plate is more concentrated toward the center of rotation than the previously proposed dual-reflector design (Figure 2), the spin momentum will
be much less. In addition, due to the microstrip design, the overall antenna volume and mass will also be much less than the dual-reflector system.

To meet the SCANSCAT's 47dBi of minimum gain requirement, approximately 65,800 microstrip patches are needed. This huge number of elements does not impact the efficiency of the antenna system since no power-dividing circuitry is needed for the reflectarray. The entire array has a diameter of 3.1 meters with a preliminarily designed feed location of 1.5 meters from the array. This 1.5 meters of feed separation (0.5 f/D ratio) is not necessarily an optimum number. If the feed gets too close to the array, the frequency excursion error will increase and therefore will narrow the operational bandwidth. If the feed is too far away from the array, the mechanical deployment and structure support problems may become severe. Certainly, the feed spillover efficiency and illumination efficiency are also determining factors in designing the feed location. This feed location optimization should be done together with a mechanical engineer.

V. Analysis of the Microstrip Reflectarray

Consider a planar array consisting of M x N microstrip patch elements that is non-uniformly illuminated by a low-gain feed at r, as shown in Figure 6. Let the desired beam direction be specified by unit value \( \hat{u} \). Then the re-radiated field in the \( \hat{u} \) direction will be of the form

\[
E(\hat{u}) = \sum_{m=1}^{M} \sum_{n=1}^{N} F(\bar{r}_{mn} \cdot \bar{r}_f) A(\bar{r}_{mn} \cdot \hat{u}_o) A(\hat{u} \cdot \hat{u}_o) \cdot
\]

\[
\exp \left(-jk[|\bar{r}_{mn} - \bar{r}_f|^2 + \bar{r}_{mn} \cdot \hat{u}] + j\alpha_{mn}\right) + E_f + E_d
\]

(1)
where $F$ is the feed pattern function, $A$ is the pattern function of the microstrip patch on the flat plate, $r_{mn}$ is the position vector of the $mn$th patch, and $\alpha_{mn}$ is the required transmission line phase delay of the $mn$th element for beam coherence. The condition that the beam will be coherent at desired direction $U_o$ is

$$\alpha_{mn} - k [ (r_{mn} - r_f) + r_{mn} \cdot U_o ] = 2n\pi, \; n = 0, 1, 2, ... \tag{2}$$

The feed function $F$ is modeled by $\cos\theta$ function. For the pattern function $A$ of the single square or rectangular microstrip patch on the flat plate, a simple closed form model using the dual-slot theory$^{(3)}$ is employed. This simple model, which is accurate enough for large array prediction, allows the computation time of many thousands of array elements to be significantly reduced. The radiation patterns of the $\theta$ and $\phi$ components from each slot of the dual-slot model, as illustrated in Figure 7, is given as follows:

$$E_\theta = -\frac{\sin (k a \cos\phi \sin\theta)}{k a \cos\phi \sin\theta} \cdot \frac{\cos (k b \sin\phi \sin\theta)}{(k b \sin\phi \sin\theta)^2 - (\pi/2)^2} \cos\theta \tag{3}$$

$$E_\phi = -\frac{\sin (k a \cos\phi \sin\theta)}{k a \cos\phi \sin\theta} \cdot \frac{\cos (k b \sin\phi \sin\theta)}{(k b \sin\phi \sin\theta)^2 - (\pi/2)^2} \sin\phi \cos\theta \tag{4}$$

where $a$ is half the dielectric thickness (slot width) and $b$ is half the patch width (slot length), and $K = 2\pi \sqrt{\epsilon_r/\lambda_0}$. The terms $E_r$ and $E_d$ in equation (1) are, respectively, the specular reflected field from the flat ground plane and the diffracted field from the edges of the ground plane. Both $E_r$ and $E_d$ are calculated via the technique of the Uniform Geometrical Theory of Diffraction$^{[2,3]}$. Although $E_r$ does not give an accurate solution for the scattered fields from the patches and the ground plane, it gives the worst solution (maximum backscattered field is reflection). This can be
assumed because the patches are separated within a very small distance (≤0.02 wavelength) from the ground plane, and the flat plate reflectarray can thus be treated RF wise as a perfect conducting plane. This is especially true at off-resonant frequencies. To accurately predict the backscattered fields from thousands of non-uniformly illuminated microstrip patches with unequal lengths of microstrip transmission lines will require the development of a complex analysis technique which is beyond the scope of the current allocated fund. The fields $E_r$ and $E_d$, no matter how accurate their calculation, are insignificant to the main beam when the array aperture gain is about 30 dB higher than the gain of the feed antenna, which is indeed the case for SCANSCAT. Nevertheless, these two terms are included in the analysis so that the worst possible sidelobe level due to scattered fields can be predicted.

The efficiency of the microstrip reflectarray is primarily governed by the aperture illumination efficiency and feed spillover efficiency\cite{8}. Aperture illumination efficiency is caused by unequal illumination of the array due to the feed pattern. The spillover efficiency is the ratio of the amount of feed energy that illuminates the entire array to the amount of energy that spills to the outside of the array. The calculation of these two efficiencies are very similar to that of a parabolic reflector. My colleague, Dr. Vahraz Jamnejad, with his many years of reflector experience, has assisted me in calculating these two efficiencies. With the $q$ factor in the feed pattern $\cos^q\theta$ chosen to be 3 and the feed separation of 1.5 meters from the 3.1-meter diameter array, the efficiency of the overall microstrip reflectarray for the SCANSCAT is calculated as following:
Table 1. Estimated microstrip reflectarray efficiency for SCANSCAT

<table>
<thead>
<tr>
<th>Type of Efficiency</th>
<th>Efficiency in Percent</th>
</tr>
</thead>
<tbody>
<tr>
<td>spillover</td>
<td>91</td>
</tr>
<tr>
<td>illumination</td>
<td>83</td>
</tr>
<tr>
<td>patch loss</td>
<td>95</td>
</tr>
<tr>
<td>feed loss</td>
<td>95</td>
</tr>
<tr>
<td>termination loss</td>
<td>95</td>
</tr>
<tr>
<td>total</td>
<td>65</td>
</tr>
</tbody>
</table>

Because the proposed microstrip reflectarray for SCANSCAT is an electrically large array, the above estimated 65% antenna efficiency is considered quite good. In addition, the illumination and spillover efficiencies may be improved by optimally designing a special feed instead of using the cosθ feed pattern.

A computer code based on the formulation in Equation (1) has been written with the FORTRAN language and user friendly inputs. For the SCANSCAT antenna, the patterns of the 36° and 49° scanned beams are calculated. For brevity's sake, only the 49° scanned beam patterns are presented here. Figure 8 gives the coordinate system of the reflectarray geometry. The radius of the reflectarray is 72 \( \lambda_0 \) and the patch elements are spaced 0.5 \( \lambda_0 \) apart, with \( \lambda_0 \) being the free space wavelength. Each patch element is 0.32 \( \lambda_0 \) x 0.32 \( \lambda_0 \) square with a substrate thickness of 0.01 \( \lambda_0 \) and a dielectric constant of 2.2. The feed has a symmetrical cosθ power pattern with \( q = 3 \) and an illumination edge taper of -9dB. Figure 9 is the calculated far field pattern in the X-Z plane when all the phase delay transmission lines on the patches are set for a beam scan of 49° in the x-z plane. The feed is located at \((X_F, Y_F, Z_F) = (0., 0., 0.)\) or \((x, y, z) = (0., 0., 72 \lambda_0)\) with an \( f/D \) ratio of 0.5. Both the feed and the patches are polarized in the Y-direction so that, when the z-axis of the array is pointed at nadir and the beam is scanned in the x-z plane, a horizontally
polarized beam is achieved. This pattern shows a 3-dB beamwidth of 0.75° and peak sidelobe level of -32dB. The beamwidth of 0.75° may be reduced down to the required 0.70° by a feed optimization program. It needs to illuminate the array more uniformly to increase the effective aperture and thus reduce the beamwidth. Figure 10 gives the $\phi$-plane pattern (constant $\theta = 49°$ plane) with a 3-dB beamwidth of 0.64° and a peak sidelobe of -31dB. The calculated directivity of this 49° scanned beam is 50.3dBi which, after subtracting 65% of efficiency loss, indicates an antenna peak gain of 48.4dBi. This is about 1.4dB above the required minimum gain.

Figure 11 gives the $\phi$-plane pattern when the feed is displaced 0.4 $\lambda_o$ in the $+y$-direction ($X_F, Y_F, Z_F = 0., 0.4 \lambda_o, 0.$), while all other parameters of the array are kept the same as those for Figures 9 and 10. The beam shows a shift of 0.34° in the $-\phi$ direction. With a second identical feed located at $Y_F = -0.4 \lambda_o$, another beam with a 0.34° shift in the $+\phi$ direction can be formed. Separate transmit and receive beams can thus be achieved for the SCANSCAT. The shifted beam shown in Figure 11 has a coma lobe at -25dB level which is still acceptable to SCANSCAT. This coma lobe distortion is a consequence of phase errors that resulted from all the phase delay lines with settings designed for a focal feed rather than an off-focal feed.

To demonstrate the effect of backscattered field components -- $E_r$ and $E_d$ of Equation (1) -- Figure 12 presents the pattern for the same antenna (diameter = 144 $\lambda_o$) as in Figure 9 except with the horizontal axis expanded and with less sampling accuracy in the pattern. This pattern does not include the effect of $E_r$ and $E_d$ and shows no far-out sidelobes above -60dB (mainbeam peak is normalized at 0dB). With this same antenna design, Figure 13 shows the pattern that does have the terms $E_r$ and $E_d$ included. Many sidelobes are near the -40dB level which is much lower than the SCANSCAT requirement. Now, let us look at a smaller reflectarray with diameter of 10 $\lambda_o$, f/D ratio of 0.5, and feed pattern q factor of
3. The far field pattern of this antenna when scanned to 36° is shown in Figure 14 where $E_r$ and $E_d$ terms are not included. For the same antenna, the scan pattern with $E_r$ and $E_d$ included is given in Figure 15 where sidelobes of -17dB level are observed. Figures 12 through 15 have demonstrated that the microstrip reflectarray antenna will not have serious high sidelobe problems caused by the backscattered fields when the aperture directivity is significantly higher (such as 30dB) than the feed directivity. In other words, the microstrip reflectarray is a more effective antenna when it is electrically large. Figure 16 plots the calculated antenna gain (estimated loss included) versus the array aperture diameter. It shows that, at the SCANSCAT frequency, the antenna gain drops much faster with reduction in aperture size when the diameter is less than one meter.

VI. Advantages and Disadvantages of the Microstrip Reflectarray

The numerous advantages of the microstrip reflectarray, in addition to its excellent application to SCANSCAT, are separately discussed below:

1. The reflectarray, being in the form of a microstrip antenna, can be fabricated with a simple, low cost, and accurate etching process. Being flat, the microstrip reflectarray will be more cost effective than the parabolic reflector when manufactured. For example, the special molding process that is generally required for fabricating a paraboloid is not needed for a flat antenna.

2. Due to the fact that no power divider is needed, the insertion loss of thousands of microstrip patches in the reflectarray will be the same as the insertion loss of a single patch and thus achieve good efficiency. The efficiency is much better than that of a conventional array with the same aperture size and is estimated to be comparable to that of a parabolic reflector (55-75% efficient).
3. The main beam of the microstrip reflectarray can be fixed to point at large angles (up to 60°) from the broadside direction, while a parabolic reflector can only have limited scan (several beamwidths). Phase shifters can be placed in the phase delay transmission lines for electronic beam scanning.

4. Since the antenna is a flat structure, its mass is likely to be less than a curved parabolic reflector with equal aperture size. It can be more easily mounted onto the surface of a structure, such as a spacecraft's main body or a building, with less supporting structure volume and mass when compared to a parabolic reflector. As a possible application, this microstrip reflectarray can be made as the world’s largest array antenna with relative ease in construction and low cost. This can be true because a flat reflectarray, where the RF loss is not a function of array size, can be constructed on flat land (aperture parallel to the land) with its feed mounted on top of a high tower. The size of the antenna is only limited by the tower height. A feed height of 1000 feet with an f/D ratio of 0.5 will result in an array with diameter of 2000 feet. This antenna size at 10 GHz can produce a pencil beam of 0.0035° in beamwidth and 95dBi of directivity.

One major disadvantage of the microstrip reflectarray is the narrow bandwidth of the microstrip patch. It is certainly no match to the wide band property of the parabolic reflector (theoretically infinite bandwidth). With conventional microstrip patch design, a maximum of 3% bandwidth can be achieved. With special design, such as a dual-stacked patch[9], the bandwidth can be increased close to 10%. The disadvantage of the narrow bandwidth of the microstrip reflectarray can be overcome somewhat by utilizing multiple-frequency operation. This is made possible for the flat reflectarray by using a multiple-layer design as shown in Figure 17 where the larger patches serve as ground planes for many of the smaller patches. A microstrip antenna having triple-frequency
capability with a three-layer design has been successfully demonstrated\cite{10}. Other multiple-frequency designs are also possible, such as multiple-ring patches and interlaced different-size patches, shown in Figure 18.

VII. Conclusion

The flat plate microstrip reflectarray antenna has been analyzed by the array theory augmented by the Geometrical Theory of Diffraction. Antenna performances, such as radiation pattern, directivity, efficiency, etc., have demonstrated that a SCANSCAT mechanically steered antenna is feasible. Its radiation efficiency is comparable to a parabolic reflector antenna, while having many mechanical advantages over a parabolic reflector. Due to its low RF loss characteristic, this antenna can be used in many large beam scanning radar applications.

VIII. References


• PEAK GAIN = 47 dBi
• POINTING KNOWLEDGE = 0.02°
• POLARIZATION = HH
• SIDELOBE LEVEL ≤ -20 dB

Figure 1. SCANSAT antenna requirements.

Figure 2. Mechanically steered dual-reflector configuration.
Figure 3. Planar array reflector antenna.

Figure 4. Flat plate microstrip reflectarray.
- TWO BEAMS IN DIFFERENT ELEVATIONS ARE SEPARATED 90° IN AZIMUTH WITH BOTH HAVING HH POLARIZATION
- 65,800 MICROSTRIP PATCHES CAN BE FABRICATED WITH SIMPLE CIRCUIT ETCHING PROCESS
- THE ARRAY REFLECTOR HAS A THICKNESS OF 0.032", THICKER HONEYCOMB – TYPE OF STRUCTURE IS NEEDED TO SUPPORT THE THIN FLAT ARRAY
- REQUIRED ANTENNA SURFACE ACCURACY < 0.030"

Figure 5. Microstrip reflectarray for SCANSCAT.

Figure 6. Coordinate system for array theory.
Figure 7. Microstrip patch dual-slot model.

Figure 8. Microstrip reflectarray coordinate system.
Figure 9. Calculated scan-plane pattern of the 49°-scanned beam.

Figure 10. Calculated φ-plane pattern of the 49°-scanned beam.
Figure 11. Calculated $\phi$-plane pattern of the 49°-scanned beam when the feed is offset in y-direction by 0.4 wavelength.

Figure 12. Calculated scan-plane pattern without including backscattered field components. Aperture diameter = 144 wavelengths.
Figure 13. Calculated scan-plane pattern with backscattered fields included. Aperture diameter = 144 wavelength.

Figure 14. Calculated scan-plane pattern without including backscattered field components. Aperture diameter = 10 wavelengths.
Figure 15. Calculated scan-plane pattern with backscattered fields included. Aperture diameter = 10 wavelengths.

Figure 16. Calculated microstrip reflectarray antenna gain versus aperture size.
Figure 17. Dual-frequency double-layer microstrip reflectarray concept.

Figure 18. Multiple-frequency microstrip reflectarray designs.
3313929*SCAN(1).SCAT(42)

C...THIS PROGRAM COMPUTES THE RADIATION PATTERN OF A LARGE
C...MICROSTRIP REFLECTARRAY WITH CIRCULAR APERTURE, ALL INPUT
C...LENGTHS ARE IN WAVELENGTH. PROGRAMMED BY DR. JOHN HUANG
C...AT JET PROPULSION LABORATORY, 12/12/1989.

DIMENSION DET(500) DBP(500) XX(500) YY(2)
COMPLEX CJ,CJJ,EXX,EYY,EZZ,FACP,EX,ET,EZ,ETH,EPH
COMPLEX ETHR,EPHR,ETH,R,EPH
COMMON/DD1/EPS,T,WT2,THER,PHR,PHR,SSP
COMMON/DD2/CJ,P,PI,PR
COMMON/DD3/XPS,YPS,FX,FY,FZ

CJ=(G.,1.)
PI=3.14159265
TPI=2.*PI
DPR=180./PI
CJJ=(1.E-15,1.E-15)

C WRITE(6,11)
C 11 _ORMAT(' MICRDSTRIP ARRAY DIMENSIONS=?'
READ(5,99)AX,BY
C WRITE(6,12)
C 12 _ORMAT(' SUBSTRATE DIELECTRIC CONSTANT & THICKNESS=?'
READ(5,99)EPS,T
C WRITE(6,13)
C 13 _ORMAT(' ELEMENT SPACING & ARRAY APERTURE RADIUS=?'
READ(5,99) DX, DY, RA
C WRITE(6,14)
C 14 _ORMAT(' FEED LOCATION & FEED COSINE Q FACTORS=?'
READ(5,99) FX, FY, FZ, QX, QY
C WRITE(6,15)
C 15 _ORMAT(' FEED POLARIZATION, IF X IP=1, IF Y IP=2'
READ(5,99)IP
C IF IP=1, BEAM NEEDS TO SCAN TO Y DIRECTION OR PHI=90 DEG FOR
C HH POLARIZATION, SCAN TO X DIRECTION OR PHI=0 DEG FOR VV
C POLARIZATION. IP=2 BEAM NEEDS TO SCAN TO X DIRECTION OR PHI=0
C FOR HH POLARIZATION, SCAN TO Y DIRECTION OR PHI=90 DEG FOR
C FOR VV POLARIZATION.
C WRITE(6,16)
C 16 _ORMAT(' REQUIRED BEAM SCAN ANGLE=?'
READ(5,99)THS,PHS
C WRITE(6,7)
C 7 _ORMAT(' PLOT X-AXIS & Y-AXIS LENGTH IN INCH=?'
READ(5,99)XDIM, YDIM
C WRITE(6,17)
C 17 _ORMAT(' PATTERN CUT ANGLE, THETA IC=1, PHI IC=2'
READ(5,99)IC
C WRITE(6,18)
C 18 _ORMAT(' LEFT BOUND, RIGHT BOUND, INCREMENT OF PLOT=?'
READ(5,99)THL, THR, ITH, PHL, PHR, IPH
C WRITE(6,19)
C 19 _ORMAT(' WRITE OUT REQUIRED ELEMENT PHASE, IF YES, IW=1'
READ(5,99)IW
C WRITE(6,20)
C 20 _ORMAT(' GTD GROUND PLANE EFFECT, IF YES, IGD=1'
READ(5,99)IGD
THSR=THSIDP
PHSR=PHSIDP

INTENTIONALLY BLANK
57 SAI = ATAN(RA/FZ)
58 CSAI = COS(SAI)
59 CSA2 = COS(SAI/2.)
60 EK1 = QX * ALOG10(CSAI)
61 EK = EK1 / 2. / ALOG10(CSA2)
62 EFF1 = (1. - CSA2 ** (2. * EK))/EK / TAN(SAI/2.)
63 EFF = (2. * EK + 1.) * EFF1 * EFF1
64 EFS = 1. - CSA2 ** (2. * (2. * EK + 1.))
65 EFI = EFF / EFS
66 WRITE(6,58) EFS, EFI, EFF
67 C58 FORMAT(* SPILL-OVER ILLUMINATION, TOTAL EFF. = *3F9.3)
68 Q1 = QX - 1
69 TQ1 = 2. * QX + 1.
70 EFS = 1. - CSAI ** TQ1
71 EF1 = (1. - CSAI ** Q1)/QX
72 EF2 = (1. - CSAI ** Q1)/Q1
73 EF3 = (1. - CSAI ** TQ1)/Q1
74 EFI = (EF1 + EF2) ** 2. / EF3
75 EFI = EFI / 2. / TAN(SAI) / TAN(SAI)
76 EFF = EFI * EFS
77 WRITE(6,59) EFS, EFI, EFF
78 C59 FORMAT(* SPILL-OVER ILLUMINATION, TOTAL EFF. = *3F9.3)
79 NX = INT(RA + 2.0000001/DX) + 1
80 NY = INT(RA + 2.0000001/DY) + 1
81 NX1 = NX - 1
82 NY1 = NY - 1
83 HFX = FLOAT(NX - 1)/2.*DX
84 HFY = FLOAT(NY - 1)/2.*DY
85 IF(I.EQ.2) GO TO 65
86 IA = ITH + 1
87 DAN = (THR - THL) / FLOAT(ITH)
88 GO TO 66
89 IA = IPH + 1
90 DAN = (PHR - PHL) / FLOAT(IPH)
91 DO 500 IJ = 1, IA
92 EXX = CJJ
93 EYY = CJJ
94 EZI = CJJ
95 IF(I.EQ.2) GO TO 67
96 THPL = THL + (IJ - 1) * DAN
97 PHL = PHL
98 GO TO 69
99 THPL = THL
100 PHL = PHL + (IJ - 1) * DAN
101 IY = 0
102 ICOUNT = 0
103 THPR = ABS(THPL)/DPR
104 PHPR = PHL/DPR
105 IF(THPL .LT. 0.) PHPR = PHL/DPR + PI
106 CT = COS(THPR)
107 CP = COS(PHPR)
108 ST = SIN(THPR)
109 SP = SIN(PHPR)
110 YP = FLOAT(NY - IY - 1) * DY - HFY
111 IX = 0
112 IY = IY + 1
113 XP = FLOAT(NX - IX - 1) * DX + HFX
114  IF(ABS(XP).LT.1.E-3) XP=1.E-8
115  IF(ABS(YP).LT.1.E-3) YP=1.E-8
116  RP=SQRT(XP*XP+YP*YP)
117  RAP=RA+0.000001
118  IF(RP.GT.RAP)GO TO 62
119  I=COUNT+1
120  SX=XP-FX
121  SY=YP-FY
122  SZ=-FZ
123  S=SQRT(SX*SX+SY*SY+SZ*SZ)
124  UX=SX/S
125  UY=SY/S
126  UZ=SZ/S
127  SXY=SQRT(SX*SX+SY*SY)
128  THF=ACOS(FZ/S)
129  PHF=ATAN2(UY,UX)
130  IF(PHF.LT.0.) PHF=PHF+TP
131  EPAT=COS(PHF)*COS(PHF)*(COS(THF))**QX+SIN(PHF)*SIN(PHF)*
132  & (COS(THF))**QY
133  SS=SQRT(SZ*SZ+RP*RP)
134  SFAC=SS-FZ
135  SFA=FLOAT(INT(SFAC))
136  PHAS1=TP+(SFAC-SFA)
137  PHN=ATAN2(YP,XP)
138  IF(PHN.LT.0.) PHN=PHN+TP
139  PHAS2=TP+RP*COS(PHR-PHN) SIN(THS)
140  PHASR=PHAS2-PHAS1
141  TES=PHASR/TP
142  ITES=INT(TES)
143  PHA0=(TES-ITES)*TPI
144  IF(I.EQ.2)GO TO 61
145  IF(I.EQ.2)GO TO 61
146  WT2=BY+T
147  DD 36 I=1,2
148  XP=X+(AX+T)/2.
149  IF(I.EQ.2) XP=X+(AX+T)/2.
150  YP=Y
151  XS=FX-XPS
152  YS=FY-YPS
153  LS=FZ
154  SSP=SQRT(XS*XS+YS*YS+ZS*ZS)
155  UXS=X/SSP
156  UYS=YS/SSP
157  UZS=Z/SSP
158  PHIR=ATAN2(-UYS,-UXS)+PI
159  IF(PHIR.LT.0.) PHIR=PHIR+TP
160  THIR=ACOS(UZS)
161  RSP=SQRT(XS*XS+YS*YS)
162  PHN=ATAN2(-UYS,-UXS)
163  IF(PHN.LT.0.) PHN=PHN+TP
164  PHAS=TP+RSP*COS(PHR-PHN) SIN(THS)
165  FACP=CEXP(CJ*(PHAS-THS))*EPAT
166  THOR=THS
167  THOR=THS
168  PHOR=PHPR
169  CALL SOURCE(EXP,EP,EP)
CALL SOURCE(EXP, EYP, EZIP)
EXX = EXP
EYY = EYP
EZZ = EZIP
ETHR = (EXX * CP * CT + EYY * SP * CT - EZZ * ST) * FACP
EPHR = (-EXX * SP + EYY * CP) * FACP
THDR = THPR
PHDR = PHPR
CALL EDGE(RA, RX, ETHD, EPHD)
ETH = ETHR + ETHD
EPH = EPHR + EPHD
AET = CABS(ETH)
AEP = CABS(EPH)
IF(AET .LT. 1.E-15) AET = 1.E-15
DBT(IJ) = 20. * ALOG10(AET)
DBP(IJ) = 20. * ALOG10(AEP)
XAX(IJ) = THPL
IF(IC.EQ.2) XAX(IJ) = PHPL
WRITE(6,77) XAX(IJ), DBT(IJ), DBP(IJ)
FORMAT(' ANGLE='F12.6, '3X,' T2T='°, F12.5, '3X, 'OBT='°, F12.5, '3X, 'DBP='°, F12.5)
CONTINUE
WRITE(6,97) ICOUNT
FORMAT(' TOTAL NUMBER OF ELEMENTS = 'I5)
YMT = -1000.
YMP = -1000.
DO 22 I = 1, IA
IF(YMT .LT. OBT(I)) YMT = OBT(I)
IF(YMP .LT. OBP(I)) YMP = OBP(I)
CONTINUE
YMX = YMT
DO 21 I = 1, IA
DBT(I) = OBT(I) - YMX
DBP(I) = OBP(I) - YMX
IF(DBT(I) .LT. -60.) DBT(I) = -60.
IF(DBP(I) .LT. -60.) DBP(I) = -60.
CONTINUE
CALL BGNPLT
CALL PLFORM(JLINLIN°, XOIM, YOIM)
XX(1) = THL
XX(2) = THR
IF(IC.EQ.2) XX(1) = PHL
IF(IC.EQ.2) XX(2) = PHR
YY(1) = -60.
YY(2) = 0.
CALL PLSCAL(XX, 2, 040504, YY, 2, 06506)
CALL PLGRAF('MICROSTRIP REFLECTARRAY\", 'ANGLE\", 'DB\")
CALL PLCURV(XAX, OBP, IA, 0, 0)
CALL PLNUP
CALL PLNTYP(5)
CALL PLNDN(0, 0)
CALL PLCURV(XAX, DBT, IA, 0, 0)
CALL ENDP LT
STOP
END
SUBROUTINE SLOTX(EXP,EYP,EZP,EX,EY,EZ)
C...THIS SUBROUTINE GIVES RE-RADIATED FIELD FROM ONE EDGE SLOT
C...OF A MICROSTRIP PATCH
COMMON/D1/EPS,THIR,PHIR,THOR,PHOR,RI
COMMON/D2/CJPI,THIR,PHIR
SPS=SQRT(EPS)
A=T/2.
B=HL/2.
CPHI=COS(PHIR)
SPHI=SIN(PHIR)
CTHI=COS(THIR)
STHI=SIN(THIR)
ARG1=PI*A*CPHI*STHI*SPS
ARG2=PI*B*SPHI*STHI*SPS
IF(ARG1.LT.1.E-4)GO TO 11
F1=SIN(ARG1)/ARG1
GO TO 12
11 F1=1.
12 IF(ABS(ARG2-PI/2.).LT.1.E-4)GO TO 13
F2=COS(ARG2)/(ARG2*ARG2-PI*PI/4.)
GO TO 14
13 F2=-1./PI
14 EPH=F1*F2*SPHI*CTHI
ETH=-F1*F2*CPHI
EXT=ETH*CTHI*C PHI-EPH*SPHI
EYT=ETH*CTHI*SPHI*EPH*CPHI
EZT=-ETH*STHI
EII=EXP*EXT
C II=EXP*EXT+EYP*EYT+EZP*EVT
CPH=COS(PHOR)
SPH=SIN(PHOR)
CTH=COS(THOR)
STH=SIN(THOR)
ARG1=PI*A*CPH*STH*SPS
ARG2=PI*B*SPH*STH*SPS
IF(ARG1.LT.1.E-4)GO TO 17
F1=SIN(ARG1)/ARG1
GO TO 18
17 F1=1.
18 IF(ABS(ARG2-PI/2.).LT.1.E-4)GO TO 19
F2=COS(ARG2)/(ARG2*ARG2-PI*PI/4.)
GO TO 20
19 F2=-1./PI
20 EPH=EII*F1*F2*SPH*CTH
ETH=EII*(-F1*F2*CPH)
FAC=CEXP(-CJ*PI*RI)/RI
EX=(ETH*CTH*CPH-EPH*SPH)*FAC
EY=(ETH*CTH*SPH*EPH*CPH)*FAC
EZ=ETH*STH*FAC
RETURN
END
SUBROUTINE SOURCE(EXP, EYP, EZP)
C...THIS SUBROUTINE GIVES SOURCE FIELD IN PATCH COORDINATE SYSTEM

COMMON/DD3/XP, YP, FX, FY, FZ, IP
IF(IP.EQ.1)GO TO 11
SX=XP-FX
SY=FZ
SZ=YP-FY
GO TO 12

11 SX=FZ
SY=YP-FY
SZ=XP-FX

12 SS=SQR(SX*SX+SY*SY+SZ*SZ)
UXS=SX/SS
UYS=SY/SS
UZS=SZ/SS
THR=ACOS(UZS)
PHR=TAN2(UY/UXS)
IF(PHR.LT.0.) PHR=PHR+PI
EX=-COS(THR)*COS(PHR)
EY=-COS(THR)*SIN(PHR)
EZ=SIN(THR)
IF(IP.EQ.1)GO TO 14
EXP=EZ
EYP=-EX
EZP=-EY
GO TO 15

14 EXP=EZ
EYP=EY
EZP=-EX

15 RETURN
END

@PRTS TT.EDG
SUBROUTINE EDGE(RA, QX, EPND, EPRE)

C SINGLE EDGE DIFFRACTED FIELDS

C COMPLEX CJ, EPND, EPRE, FAC, FAC

C COMPLEX DS, OH, DPS, OPH

C COMMON/DD1/EPS, T, HL, TTHIR, PHIR, THOR, PHOR, RI

C COMMON/DD2/CJ, PI, TP1, DPR

C COMMON/DD3/XP, YP, FX, FY, FZ, IP

XP = RA
YP = 0.

CALL SOURCE(EX, EY, EZ)
THOR = ATAN(FZ/RA)
EPAT = COS(P1/2. - THOR)**QX
EPNI = EX*SIN(THOR) + EZ*COS(THOR)
EPRI = EY
R = RA*COS(THOR)
FAC = EXP(-CJ*TP1*R)/R*EPAT
PHP = THOR*DPR
PH = THOR*DPR + 90.

IF(PHOR.GT.0.01) PH = 90. - THOR*DPR
CALL DW(DS, OH, DPS, OPH, R, PHP, PH, 90., 2.)

ENI = COS(THOR)
ENS = COS(P1/2. - THOR)

IF(PHOR.GT.0.01) ENS = COS(P1/2. + THOR)
SGD = (1./R) - (ENI-ENS)/RA
RHO = ABS(1./SGD)

FACP = EXP(CJ*TP1*RA*SIN(THOR))

IF(PHOR.GT.0.01) FACP = EXP(-CJ*TP1*RA*SIN(THOR))

EPND = EPNI*FAC*OH*SQRT(RHO)*FACP
EPRE = EPRI*FAC*OS*SQRT(RHO)*FACP

IF(SGD.LT.0.) EPND = EPND*CJ
IF(SGD.LT.0.) EPRD = EPRD*CJ

CALL SOURCE(EX, EY, EZ)
EPNI = EX*SIN(THOR) - EZ*COS(THOR)
EPRI = EY

PH = 90. - THOR*DPR

IF(PHOR.GT.0.01) PH = THOR*DPR + 90.

CALL DW(DS, OH, DPS, OPH, R, PHP, PH, 90., 2.)

ENS = COS(P1/2. + THOR)

IF(PHOR.GT.0.01) ENS = COS(P1/2. - THOR)
SGD = (1./R) - (ENI-ENS)/RA
RHO = ABS(1./SGD)

FACP = EXP(-CJ*RA*TP1*SIN(THOR))

IF(PHOR.GT.0.01) FACP = EXP(CJ*RA*TP1*SIN(THOR))

EPND = EPNI*FAC*OH*SQRT(RHO)*FACP
EPRE = EPRI*FAC*OS*SQRT(RHO)*FACP

IF(SGD.LT.0.) EPND = EPND*CJ
IF(SGD.LT.0.) EPRD = EPRD*CJ

RETURN
END
SUBROUTINE DW(DS,DH,DPS,DPH,R,PH,PHP,BO,FN)

C *** WEDGE DIFFRACTION AND SLOPE DIFFRACTION COEFFICIENT ***

C *** FOR THE SOFT AND HARD B.C. ***

COMPLEX DIN,DIP,DPN,DPP,DS,DH,DPS,DPH

BETN=PH-PHP

CALL D(DIN,R,BETN,BO,FN)

CALL DPI(DPN,R,BETN,BO,FN)

IF(ABS(PHP).GT.2.5E-4.AND.ABS(PHP).LT.(FN*180.-2.5E-4))

$) GO TO 10

DS=(O.,O.)

DH=DIN

DPS=DPN

DPH=(C=,O.)

RETURN

10 CONTINUE

BETP=PH+PHP

CALL DI(DIP,R,BETP,BO,FN)

CALL DPI(DPN,R,BETP,BO,FN)

DS=DIN-DIP

DH=DIN+DIP

DPS=DPN+DPP

DPH=DPN-DPP

RETURN

END

@PRINTS TT.DI

-35-
SUBROUTINE OICDIR,R,_ET,BO,FN)
INCIDENT (BET=PH-PHP) OR REFLECTED (BET=PH+PHP)
***
PART OF WEDGE DIFFRACTION COEFFICIENT ***

DATA PI,TPI,DER/3.14159265,6.2831853,57.29577958/
ANG=BET/DR
TOP=-CEXP(CMPLX(0.,-PI/4.))
DEM=2.*TPI*FN*SIN(BO/DPR)
COM=TOP/DEM
SQRT(TPI*R)
DNS=(PI+ANG)/(2.0*FN*PI)
SGN=SIGN(1.,DNS)
N=IFIX(ABS(DNS)+0.5)
DN=SGN*N
A=1.0+COS(ANG-2.0*FN*PI*ON)
BOTL = 2.0*SQRT(ABS(R*A))
EX=CEXP(CMPLX(0.0,TPI*R*A))
CALL FRNELS (C,S,BOTL)
C=SQRT(PI/2.0)*(-0.5-C)
S= SQRT(PI/2.0)*(S-0.5)
FA=CMPLX(0.,2.)*SQR*EX*CMPLX(C,S)
RAG=(PI+ANG)/(2.0*FN)
TSIN=TN(RAG)
TS=ABS(TSIN)
IF(TS.GT.1.E-5) GO TO 442
COTA=-SQRT(2.0)*FN*SIN(ANG/2.0*FN*PI*ON)
IF(COS(ANG/2.0*FN*PI*ON).LT.0.0) COTA=-COTA
GO TO 443
COTA=SQRT(A)*COS(RAG)/TSIN
UPPI=COM*COTA*FA
DNS=(-PI+ANG)/(2.0*FN*PI)
SGN=SIGN(1.,DNS)
N=IFIX(ABS(DNS)+0.5)
DN=SGN*N
A=1.0+COS(ANG-2.0*FN*PI*ON)
BOTL = 2.0*SQRT(ABS(R*A))
EX=CEXP(CMPLX(0.,TPI*R*A))
CALL FRNELS (C,S,BOTL)
C=SQRT(PI/2.0)*(-0.5-C)
S= SQRT(PI/2.0)*(S-0.5)
FA=CMPLX(0.,2.)*SQR*EX*CMPLX(C,S)
RAG=(PI-ANG)/(2.0*FN)
TSIN=TN(RAG)
TS=ABS(TSIN)
IF(TS.GT.1.E-5) GO TO 542
COTA= SQRT(2.0)*FN*SIN(ANG/2.0*FN*PI*ON)
IF(COS(ANG/2.0*FN*PI*ON).LT.0.0) COTA=-COTA
GO TO 123
COTA=SQRT(A)*COS(RAG)/TSIN
UPPI=COM*COTA*FA
DIR=UPPI+UNPI
RETURN
END
SUBROUTINE DPI(DPIR,R,BET,BO,FN)
  C *** INCIDENT (BET=PH-PHP) OR REFLECTED (BET=PH+PHP) ***
  C *** PART OF WEDGE SLOPE DIFFRACTION COEFFICIENT ***
  COMPLEX TOP,COM,EX,UPPI,UNPI,FPA,DPIR
  DATA PI,TPI,DPRI,3.14159265,6.2831853,57.29577958/
  ANG=BET/DPR
  SBO=SIN(BO/DPR)
  TOP=CEXP(CMPLX(0.,-PI/4.))
  DEM=4.*TPI*FN*FN*SBO*SBO
  COM=TOP/DEM
  DNS=(PI+ANG)/(2.0*FN)
  SGN=SIGN(1.,DNS)
  N=IFIX(ABS(DNS)+0.5)
  DN=SGN*N
  A=1.0*COS(ANG-2.0*FN*PI*DN)
  BOTL = 2.0*SQRT(ABS(R*A))
  EX=CEXP(CMPLX(0.0,TPI*R*A))
  CALL FRNELS (C,S,BOTL)
  C=SQRT(TPI/2.0)*(0.5-C)
  S= SQRT(TPI/2.0)*(S-0.5)
  FPA=TPI*R*(CMPLX(0.0,4.*SQRT(ABS(TPI*R*A))*EX*CMPLX(C,S))
  RAG=(PI+ANG)/(2.0*FN)
  TSIN=SIN(RAG)
  TS=TSIN*TSIN
  IF(TS.GT.1.E-5) GO TO 442
  CSCA=-2.*FN*FN*COS(ANG-TPI*FN*DN)/COS((PI+ANG)/FN)
  GO TO 443
  C=-(PI+ANG)/(2.0*FN)
  SGN=SIGN(1.,DNS)
  N=IFIX(ABS(DNS)+0.5)
  DN=SGN*N
  A=1.0*COS(ANG-2.0*FN*PI*DN)
  BOTL = 2.0*SQRT(ABS(R*A))
  EX=CEXP(CMPLX(0.0,TPI*R*A))
  CALL FRNELS (C,S,BOTL)
  C=SQRT(TPI/2.0)*(0.5-C)
  S= SQRT(TPI/2.0)*(S-0.5)
  FPA=TPI*R*(CMPLX(0.0,4.*SQRT(ABS(TPI*R*A))*EX*CMPLX(C,S))
  RAG=(PI+ANG)/(2.0*FN)
  TSIN=SIN(RAG)
  TS=TSIN*TSIN
  IF(TS.GT.1.E-5) GO TO 542
  CSCA=-2.*FN*FN*COS(ANG-TPI*FN*DN)/COS((PI+ANG)/FN)
  GO TO 123
  C=-(PI+ANG)/(2.0*FN)
  UNPI=COM*CSCA*FPA
  DPIR=UPPI-UNPI
  RETURN
END
SUBROUTINE FRNELS(C,S,XS)
THIS IS THE FRESNEL INTEGRAL SUBROUTINE WHERE THE INTEGRAL IS FROM
U=0 TO XS, THE INTEGRAND IS EXP(-J*PI/2.*U*U) AND THE OUTPUT IS
C(XS)-J*S(XS).
DIMENSION A(12),B(12),CC(12),O(12)
DATA A/1.595769140,-0.000001702,-1.56850-0.000576361,6.920691
+02,-0.016898657,-3.05486560-0.075752419,0.850663781-0.02563904
+1.0,0.150230960,0.034404779/
DATA B/-0.000000033,4.25387524,-0.000092810,-7.80002400,-0.000952
*+9955.075561298,-0.138314947,-1.36379214,-0.403349276,0.70222011
+8.0.216195929,0.019547031/
DATA CC/0.000000033,4.25387524,0.000000039,0.005770956,0.00068982,-0.009
*+19713,0.0119488809,-0.036748873,0.000246420,0.002102967,0.0012179
+30.000233939/
DATA 0/0.19471140,0.00000023,-0.009351341,0.000023006,0.00485146
*+6.0001903218,-0.017122914,0.029064076,-0.027923955,0.016497303,-3
+*.005598515,0.000838386/
DATA PI/3.14159265/
IF(XS.LE.0.0) GO TO 414
X=XS
X= PI*X*X/2.0
FR=0.0
FI=0.0
K=13
IF(X-4.0)
+10,40,40
Y=X/4.0
10
Y=X/4.0
20
K=K-1
28
FR=(FR+A(K))*Y
29
FI=(FI+B(K))*Y
30
IF(K-2) 30,30,20
31
FR=FR+A(1)
32
FI=FI+B(1)
33
C=(FR*COS(X)+FI*SIN(X))*SQRT(Y)
34
S=(FR*SIN(X)-FI*COS(X))*SQRT(Y)
35
RETURN
36
40
Y=4.0/X
37
50
K=K-1
38
FR=(FR+CC(K))*Y
39
FI=(FI+D(K))*Y
40
IF(K-2) 60,60,50
41
60
FR=FR+CC(1)
42
FI=FI+O(1)
43
C=0.5*(FR*COS(X)+FI*SIN(X))*SQRT(Y)
44
S=0.5*(FR*SIN(X)-FI*COS(X))*SQRT(Y)
45
RETURN
46
414
C=-0.0
47
S=-0.0
48
RETURN
49
END

TP=10.368  SUP=6.107  CPU=.009  ID=2.609  CC-ER=3.488

BRKPT PRINTS
This publication presents an antenna system that has been proposed as one of the candidates for the SCANSCAT (Scanned Scatterometer) radar application. It is the mechanically steered planar microstrip reflectarray. Due to its thin, lightweight structure, the antenna's mechanical rotation will impose minimum angular momentum for the spacecraft. Since no power-dividing circuitry is needed for its many radiating microstrip patches, this electrically large array antenna demonstrates excellent power efficiency. In addition, this fairly new antenna concept can provide many significant advantages over a conventional parabolic reflector.

The basic formulation for the radiation fields of the microstrip reflectarray is presented. This formulation is based on the array theory augmented by the Uniform Geometrical Theory of Diffraction (UTD). A computer code for analyzing the microstrip reflectarray's performances, such as far-field patterns, efficiency, etc., is also listed in this report. It is proposed here that a breadboard unit of this microstrip reflectarray should be constructed and tested in the future to validate the calculated performance. The antenna concept presented here can also be applied in many other types of radars where a large array antenna is needed.