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Impedance matched absorptive thermal blocking filters

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We have designed, fabricated, and characterized absorptive thermal blocking filters for cryogenic microwave applications. The transmission line filter’s input characteristic impedance is designed to match 50 Ω and its response has been validated from 0 to 50 GHz. The observed return loss in the 0 to 20 GHz design band is greater than 20 dB and shows graceful degradation with frequency. Design considerations and equations are provided that enable this approach to be scaled and modified for use in other applications. [http://dx.doi.org/10.1063/1.4869038]

I. INTRODUCTION

Thermal blocking filters find wide use in cryogenic applications ranging from quantum computing to ultra-low-noise detectors. They can be used to provide the environmental isolation between cooled devices and the warmer temperature supporting bias and readout circuitry. In particular, they are effective in rejecting thermal radiation, limiting radio frequency interference, providing a convenient means of heat sinking signal lines, and realizing a vacuum feedthrough. In a microwave instrumentation setting a well-defined characteristic impedance, typically approximating a short or matched boundary condition, is desirable. From a radiometric perspective, such filter structures limit the available power by modifying the transmitted response and effectively reducing the photon density of states in the Planck distribution to a single dimension.

A variety of thermal blocking filter construction techniques and designs have been discussed in the literature. In the device’s most basic form, a large shunt capacitor forms a single-pole low-pass filter. More generally, multiple low-pass lumped element stages can be combined in series to produce compact and broadband non-dissipative filter structures. The challenges presented by these implementations include controlling inter-stage isolation and spurious transmission resonances, limiting the filter’s total shunt capacitance, and achieving adequate control over circuit parameters as a function of temperature. Dissipative solutions based on distributed lossy microwave structures can be used to achieve a broadband low-pass transmission response. More recent efforts have strived to retain these desirable properties while providing a well defined impedance match. Specific examples in this class include coaxial-lines and strip-line powder filters.

In this work, simple matched filter designs based on easily realized absorptive dielectric transmission lines are improved upon, and the resulting performance is described in detail. The filter’s response is predictable, repeatable under cryogenic cycling, and is capable of providing an intrinsically broadband matched impedance termination. In Sec. II, practical design considerations and the governing equations for the filter’s operation are described in detail. The fabrication and test of the representative filters are summarized in Sec. III.

II. DESIGN METHOD AND CONSIDERATIONS

In order to minimize reflections in an absorptive transmission line filter, the modal symmetry, geometric overlap, and impedance of the lines and interface discontinuities need to be appropriately matched. From this perspective, with appropriate attention to detail, a tube with a centered wire and lossy dielectric lends itself to fulfill the desired low-pass filter functions. The structure can be easily fabricated via direct machining with readily available materials and can provide reliable operation in a cryogenic environment. See Figure 1 for a sketch of the filter geometries explored and characterized here.

A simplified microwave model that assumes a constant dielectric function and retains the qualitative response of the device is presented. The first step is to select a realizable geometry and lossy medium that present a characteristic impedance equal to that of the measurement system. The characteristic impedance of a single wire in a square enclosure can be expressed as a perturbative expansion on a coaxial line or in closed form through the introduction of a shielding factor as follows:

$$Z_o = \frac{\eta_o}{2\pi} \left( \frac{\mu_r}{\epsilon_r} \right)^{1/2} \cdot \ln \left( \frac{D}{d} \cdot s \cdot (D/d) \right),$$

where $\mu_r$ and $\epsilon_r$ are the relative permeability and permittivity of the media between the inner and outer conductors in the filter, respectively, and $\eta_o = (\mu_o/\epsilon_o)^{1/2} \approx 377 \Omega$ per square is the wave impedance of free space. Here $D$ is the width (height) of the channel and $d$ is the center conductor outer diameter. The shielding factor, $s(D/d)$, is a weak monotonically increasing function for this topology. Numerical simulations for a circular wire in a square enclosure reveal $s(1.1) \approx 0.6422$ and rapidly approaches a limiting asymptote, $s(\infty) \rightarrow 1.07871$, for $D/d > 3$.

Similarly, the impedance of a wire centered between ground parallel planes can be computed from the above expression by adopting a shielding factor of $s(D/d) = 4/\pi$. For a coaxial transmission line, the shielding factor, $s(D/d)$, is unity and $D$ is taken as the inner diameter of the outer conductor.

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III. FILTER FABRICATION AND TEST

In the matched filter implementations explored, a stainless-steel wire (≈0.2 mm outer diameter) serves as the center conductor and a metal housing forms the metallization for line’s outer conductor. The stainless steel wire diameter was selected to be compatible and make a reliable light press fit into the SMA (SubMiniature version A) connector’s rear socket (Southwest Microwave, Tempe AZ; model number 214-537SF; nominal pin inner diameter ≈0.225 mm, pin insertion depth ≈2 mm). This connector supports a single transverse electromagnetic mode through ~27 GHz, and the filter provides sufficient attenuation to prevent spurious resonances in the structure and degradation of the impedance response. The measured total DC resistance of the connectorized structures (e.g., <1.4 Ω for the square channel filter described) is observed to be within 4% of the value computed for 304 stainless and the center conductor line geometry. This can be reduced by employing a copper clad stainless magnet wire or a superconducting center conductor if compatible with the desired end application.

A dielectric mixture comprised of epoxy (Ellsworth Adhesives, Germantown, WI; Emerson-Cumming 2850 FT with Catalyst 23LV) loaded with a volume filling fraction ≃ 0.3 of stainless-steel powder21 is used to fill the volume between the center and outer conductor forming a controlled impedance transmission line. The dielectric permittivity and magnetic permeability of this loading are εr ≈ 10.6 + 2.1i and μr ≈ 1, respectively. This choice represents the highest permittivity mixture that has flow characteristics compatible with filling the desired volume and minimizes the envelope of the filter package. Using Eq. (1) to achieve an impedance match to a 50 Ω line, a D/d ~ 15 ratio should be targeted when using this dielectric mixture. Reflections at the ~26 dB level are anticipated in evaluating the reflectance in Eq. (2). The ratio of power attenuation coefficient over the operating frequency in gigahertz, \[ \frac{\alpha}{\nu} \approx 0.005 \text{ (dB/mm)/GHz}, \] where the uncertainty is bounded by the observed variation in dielectric mixture’s loss. The real component of the dielectric permittivity as a function of the volume filling fraction has a lower impact on the overall filter response.
The metal housings for these filters are realized by either drilling a circular hole through a block or milling a square channel in a split-block as indicated in Figure 1. The primary objective in potting the filter is to achieve a homogenous dielectric mixture free of voids between the transmission line’s center and outer conductors. This goal can be readily achieved for the square channel split-block filter configuration. The top surface of the milled block is temporarily masked with Kapton tape, the channel filled with epoxy, cured, and subsequently lapped smooth to realize a low impedance metal-to-metal contact between the flat surfaces of the body and the cover. An average surface roughness, $R_A \leq 0.2 \mu m$, is specified for the finish at all mating surfaces to achieve the desired RF seal.

In the drilled filter housing approach, a 0.98 mm diameter hole approximately 3 diameters in length, is made near each end of the tube for filling with epoxy and venting gas from the volume. The SMA connectors are installed in order to locate the transmission line center conductor during potting. This arrangement precisely defines the desired volume and allows the epoxy mixture to be injected into the filter with a syringe without entrapping bubbles. Once the cavity is filled with epoxy, the fill and vent holes are plugged with a 19 gauge wire (0.91 mm outer diameter) to be flush with the inner tube wall. This defines an electrically short lossy line section with $\approx 5 \Omega$ characteristic impedance which is small compared to the signal line $Z_o$. As a result, the arrangement has a negligible influence on the RF match at the SMA ports.

The residual loaded epoxy was used to make a pair of witness samples in WR28.0 waveguide of differing physical lengths. After curing the witness samples, the scattering parameters were measured with an Agilent PNA-X Vector Network Analyzer (VNA) from 26 to 40 GHz with a TRL (Thru-Reflect-Line) calibration. A two-line matrix technique was used to extract and verify the electromagnetic properties of the mixture employed in each filter structure. The scattering parameters of the filters were measured at room temperature and $\sim 4$ K. For these measurements the VNA was calibrated with a SOLT (Short-Open-Line-Thru) calibration in 2.4 mm 50 $\Omega$ lines where the reference planes reside at the test device’s SMA connectors. The parameters for the filters characterized are described in Table I and the response summarized in Figure 2. The measurements are consistent with a transmission line model calculation for the as built geometry and fabrication tolerances.

We have also realized variations on the fabrication scheme described for filtering arrays of multiple signal lines in a wide channel with an alternative dielectric mixture.

For the six-line filter example depicted in Figure 1, polytetrafluoroethylene (PTFE) shims were used to temporarily hold the conductors in place within a milled channel. The steel-powder was then poured to fill the filter volume. Once assembled, a ~2 centipoise cyanoacrylate (i.e., “low-viscosity superglue”) was wicked through the powder and cured to realize the lossy dielectric insert. This mixture formulation’s relatively large permittivity, $\varepsilon_r \sim 20 + 20i$, correspondingly shrinks the dimensions required to maintain a given level of mode conversion, increases the tolerances to control the impedance, and increases the line attenuation ($\alpha/\nu_{GHz} \approx 0.37 \pm 0.04$ (dB/mm)/GHz) in principle, the permittivity can be further increased by employing a disordered alloy with a higher conductivity than stainless steel or by incorporation of magnetic materials in the mixture. The mixture’s relatively large dielectric loss tangent tends to degrade the filter’s input impedance (e.g., a return loss of $\sim 14$ dB is computed for the formulation described), however, it enables a $>24$ dB inter-line isolation to be achieved between adjacent lines. Use of every other line as a grounded guard line or terminating in the system’s characteristic impedance would enable a modest improvement in isolation over this level; however, this reduces the available density of signal lines and may provide undesired signal return paths for low-noise applications. After removal of the PTFE shims, the top surface of the filter was lapped smooth for electrical contact between the body and cover. In this example, the total channel width is 36 mm with an interline spacing $= 2.5$ mm was implemented. A summary of the measured filter response is presented in Figure 3.

### Table I. Thermal blocking filter geometric parameters.

<table>
<thead>
<tr>
<th>Filter housing construction</th>
<th>Milled channel</th>
<th>Drilled hole</th>
<th>6-line channel</th>
<th>Units</th>
</tr>
</thead>
<tbody>
<tr>
<td>Inner conductor, $d$</td>
<td>0.200</td>
<td>0.200</td>
<td>0.16</td>
<td>mm</td>
</tr>
<tr>
<td>Outer conductor, $D$</td>
<td>3.2</td>
<td>3.0</td>
<td>36</td>
<td>mm</td>
</tr>
<tr>
<td>Filter length, $L$</td>
<td>62.5</td>
<td>38.9</td>
<td>13</td>
<td>mm</td>
</tr>
<tr>
<td>Shielding factor, $s$</td>
<td>$\approx 1.079$</td>
<td>1</td>
<td>$4/\pi$</td>
<td></td>
</tr>
</tbody>
</table>
Recall that the filter in question is matched and the filter response described by Eq. (2) is well approximated by $F(ν) ≃ \exp (-4πκLν/κc) = \exp (-4πκLν/c)$, and an analytical evaluation of the desired expression can be derived. For convenience we define a dimensionless constant, $β ≡ 4πκLk_b T c$, change variables to $x = hν/k_b T$, and find,

$$P = \frac{(k_b T)^2}{h} \int_0^∞ \frac{e^{-(1+β)x}}{1 - e^{-x}} \, dx.$$  \hspace{1cm} (A2)

By expanding the denominator as a geometric series,

$$P = \frac{(k_b T)^2}{h} \int_0^∞ xe^{-(1+β)x} \sum_{n=0}^∞ e^{-nx} \, dx,$$

interchanging the order of integration and the summation and changing variables to $ζ = (1 + β + n) \cdot x$ yields,

$$P = \frac{(k_b T)^2}{h} \sum_{n=0}^∞ \frac{1}{(1 + β + n)^2} \int_0^∞ ζ e^{-ζ} \, dζ.$$  \hspace{1cm} (A4)

Noting that the sum over $n$ gives the trigamma function $\psi''(1 + β)$ and the integral is $Γ(2) = 1$, enables the coupled power to be expressed as follows:

$$P = \frac{(k_b T)^2}{h} \cdot ψ''(1 + β),$$  \hspace{1cm} (A5)

where the trigamma function can be evaluated numerically or via its recursion relation, $ψ''(1 + β) = ψ'(β) - 1/β^2$, for $β > 0$. With a lossless line, $ψ'(1) = π^2/6$, and Eq. (A5) gives the physically anticipated power emitted by a 1D blackbody spectrum.\(^{26,27}\) Recalling $β$ is a dimensionless measure of the filter’s roll-off frequency over the blackbody’s characteristic response, for the thermal block design to be effective, $β ≫ 1$. Evaluating $ψ''(β) → 1/β$ in its asymptotic limit we obtain an approximate form for the residual coupled power encountered in practical applications,

$$P \simeq \frac{(k_b T)^2}{hβ} = k_b T \cdot \frac{c}{4πκL} = k_b T \cdot Δν_{eff},$$  \hspace{1cm} (A6)

where $Δν_{eff} ≡ c/4πκL ≃ ν_{0.5}/ln (2)$ is the effective radiometric signal bandwidth and $ν_{0.5}$ is frequency of the thermal blocking filter’s half-power response. The product, $Δν_{eff} \cdot L ≃ 80 \, GHz \, mm$, is estimated for a matched filter with $κ_r \simeq 10.6 + 2.11$ and $μ_e \approx 1$ when used in the manner described.

\begin{enumerate}
\end{enumerate}


